

## ***Improved Load Current Capability for Cap-Drop Off-Line Power Supplies for E-Meter Using the TPS5401***

Sankar Sadasivam, Harmeet Singh, Michael Gilbert, Steven Schnier, Michael Green, and Amy Ball

*Power DC/DC Controllers*

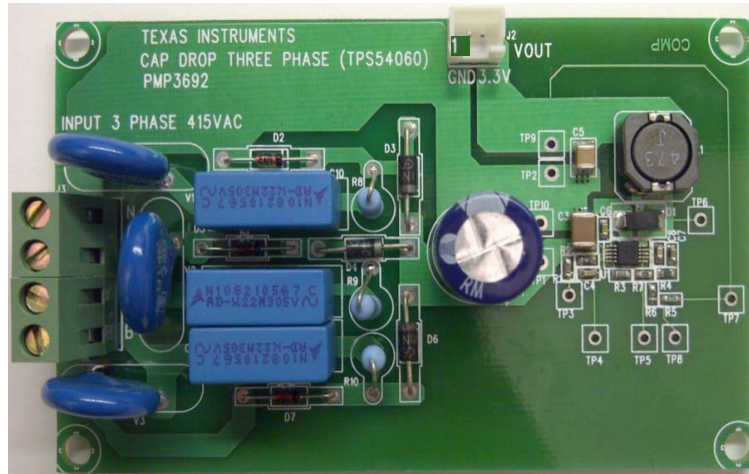
### **ABSTRACT**

Standard electronic electricity meters (e-meters) have traditionally used a capacitive-drop power supply (cap-drop) plus linear regulator topology to provide a cost-effective power supply. Today, opposing forces such as an increase in load currents due to more complex AMR and AMI communications circuitry and tighter power consumption regulations, force e-meter designers to limit consumption to below 4VA (~1.2W) for single-phase or 8VA (~2.4W) for 3-phase e-meters. Employing an innovative, yet simple, solution using a switching DC/DC converter, such as the TPS5401 in place of the linear regulator allows the e-meter designer to avoid the costly move to expensive switch mode power supply (SMPS) solutions. This application note goes through the step-by-step decisions a designer must make to complete a cap-drop power supply with a DC/DC converter. A design calculator tool, SLVC392, is also available with the application note to assist the designer, when the design criteria are different than the application note.

The concept shown in this application note can also be expanded to a 3-phase application that requires more load current. Both applications have been built and tested and are available for download as PMP6960 (single phase with the TPS5401) and PMP3692 (three phase with the TPS54060).



**Figure 1. Single Phase Cap Drop E-Meter Design (PMP6960) using the TPS5401**



**Figure 2. Three Phase Cap Drop E-Meter Design (PMP3692) using the TPS54060**

**Contents**

<b>Capacitor Drop Design .....</b>	<b>4</b>
Isolation Cap Selection and Input Current Considerations .....	4
Input Voltage .....	4
Output Voltage and Output Current .....	5
Duty Cycle and Frequency Set Resistor .....	5
Inductor .....	6
Output Capacitor .....	6
Diode Selection .....	7
Compensation and Frequency Response .....	7
Input Capacitors .....	8
Slow Start Time .....	9
Power Dissipation .....	9
FET .....	9
Internal IC .....	10
Pre-Converter .....	10
Low Side Catch Diode and Inductor .....	10
Input of Converter .....	11
<b>Appendix A. Experimental Results .....</b>	<b>12</b>
A.1 Efficiency .....	12
A.2 Control Loop .....	13
A.3 $V_{IN}$ Ripple .....	15
A.4 $V_{OUT}$ Ripple .....	16
A.5 Slow-Start .....	18
A.6 Surge Test .....	18

**Figures**

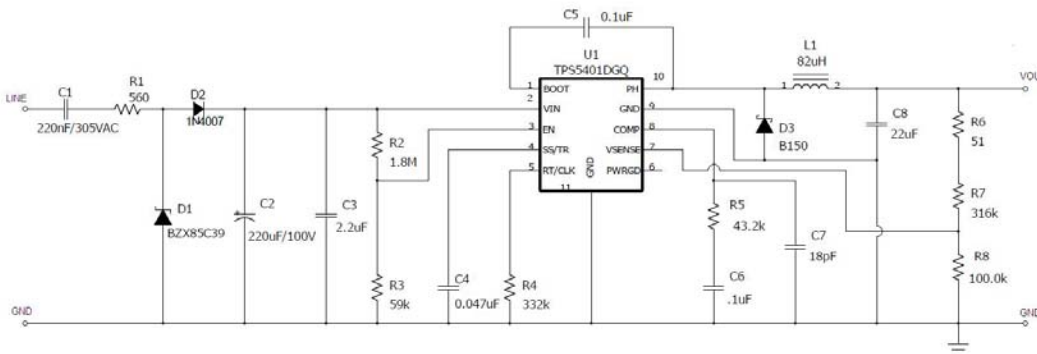
Figure 1. Single Phase Cap Drop E-Meter Design (PMP6960) using the TPS5401 ..... 1  
 Figure 2. Three Phase Cap Drop E-Meter Design (PMP3692) using the TPS54060..... 2  
 Figure 3. Schematic of Cap Drop E-Meter Design (PMP6960) using the TPS5401 ..... 3  
 Figure A-1. DCM Design Efficiency..... 12  
 Figure A-2. Logarithmic DCM Design Efficiency ..... 12  
 Figure A-3. Frequency Response at 40mA Load..... 13  
 Figure A-4. Load Regulation at 3.3V<sub>OUT</sub>..... 14  
 Figure A-5. Line Regulation at 3.3V<sub>OUT</sub>..... 14  
 Figure A-6. V<sub>IN</sub> Ripple at 5mA Load ..... 15  
 Figure A-7. V<sub>IN</sub> Ripple at 40mA Load ..... 15  
 Figure A-8. V<sub>IN</sub> Ripple at 50mA Load ..... 16  
 Figure A-9. V<sub>OUT</sub> Ripple at 5mA..... 16  
 Figure A-10. V<sub>OUT</sub> Ripple at 40mA..... 17  
 Figure A-11. V<sub>OUT</sub> Ripple at 50mA..... 17  
 Figure A-12. Slow-Start vs. EN ..... 18  
 Figure A-13. Slow-Start vs. V<sub>IN</sub> ..... 18

**Tables**

Table 1. Power Supply Requirements ..... 3

**Table 1. Power Supply Requirements**

Input Voltage (V <sub>IN</sub> )	230VAC 50Hz (nominal) – 50mA Load 80VAC 50Hz (min)– 12.5mA load 305VAC 50Hz (max)– 66.8mA load
Input Current (4VA limit)	17.4mA
Output Voltage	3.3V
Output Voltage Ripple	1%
Maximum Output Current	50mA
Switching Frequency	365kHz



**Figure 3. Schematic of Cap Drop E-Meter Design (PMP6960) using the TPS5401**

Note: There was no Metal Oxide Varistor (MOV) at the input to demonstrate robust performance without any additional components.

## Capacitor Drop Design

### Isolation Cap Selection and Input Current Considerations

Apparent Power, described in Volt-Amperes (VA) =  $V_{RMS} \times I_{RMS}$ . Under the existing restrictions, if the apparent power must be limited to 4VA with an AC line voltage ( $V_{RMS}$ ) of 230V, then  $I_{RMS}$  needs to be limited to 17.4mA. The size of the input capacitor will limit the amount of AC current into the system. Using equation (1), where  $V_{RMS} = 230V$ ,  $f = 50Hz$ , and  $I_{RMS} = 17.4mA$ , then  $C_{IN}$  must be  $\leq 240nF$ . A standard value of 220nF is chosen for this design, with a voltage rating of 305VAC.

$$C_{IN} = \frac{I_{RMS}}{(V_{RMS} \times 2 \times \pi \times f)} \quad (1)$$

If chosen correctly, the capacitor drop and half wave rectifier will protect the circuit from line surges. (See appendix A.7)

### Input Voltage

The resulting DC current through a half-wave rectifier into the voltage regulator can be calculated with equations 2-5. With  $V_{AC} = 230V$ ,  $C_{IN} = 220nF$ ,  $V_z = 39V$  and  $D = .5$ , the resulting  $I_{DCIN} = 7mA$ . For a linear regulator,  $I_{DCOUT} = I_{DCIN}$ ; therefore, at  $\sim 7mA$  max, linear regulators can be used with a cap-drop supply for only the simplest of single phase e-meters. For higher load demands, a switching DC/DC converter, such as the TPS5401, is required.

$$I_{IN\ HRMS} = (V_{PEAK} - V_z) \times \pi \times 50Hz \times C_{IN} \quad (2)$$

$$V_{IN\ RMS} = V_z \times \sqrt{D} \quad (3)$$

$$P_{IN} = I_{IN\ RMS} \times V_{IN\ RMS} \quad (4)$$

$$I_{INDC} = \frac{P_{IN}}{V_{INDC}} \quad (5)$$

When a switching DC/DC converter is used, a boost in efficiency complements the design. By predicting the efficiency and using equations 6 and 7, the power out and  $I_{OUT}$  can be found. The higher the regulator input voltage and the higher the efficiency, the larger the output current can be. In this example, the TPS5401 is chosen, with an input voltage of 42V. Other devices can be used, such as the TPS54060 or TPS54062 for higher input voltage and higher efficiency. These additional devices are supported in the calculator tool, SLVC392.

$$I_{OUTDC} = \frac{P_{OUT}}{V_{OUT}} \quad (6)$$

$$P_{OUT} = P_{IN} \times \eta \quad (7)$$

(where  $\eta$  = efficiency of the converter at the intended DC load current)

Using the equations 2-7 with the TPS5401 (with a  $V_{IN}$  max of 41V to account for variation in the zener diode,  $\eta \approx 60\%$  at desired operating point, and a desired  $V_{OUT}$  of 3.3V), we can get as much as 50mA into the load at 230VAC. This is reduced to 12.5mA at 80VAC.

The efficiency can be optimized by choosing the switching frequency, output cap and inductor, as well as minimizing losses through other components such as the output voltage setting resistors and adjustable UVLO resistors. Equations 8 and 9 will derive the UVLO resistor values. Use equation 10 to find the power dissipated through the resistors. If the  $V_{start}$  and  $V_{stop}$  values are too low, there will not be enough current to charge the input capacitors and operate the converter at start up. In order to prevent this, set  $V_{start}$  as close as possible to  $V_{INMIN}$  and  $V_{stop}$  to be within 20% of  $V_{INMIN}$ . For this design,  $V_{start} = 37V$  and  $V_{stop} = 32V$ . Using equations 8 and 9  $R2 = 1.7M$ , but a 1.8M was used and  $R3 = 58K$ , but a 59K was used.

$$R2 = \frac{V_{start} - V_{stop}}{I_{hys}} \quad (8)$$

$$R3 = \frac{V_{ena}}{\frac{V_{start} - V_{ena}}{R1} + I1} \quad (9)$$

## Output Voltage and Output Current

Most loads require a single input voltage of 3.3V. Adjusting the output voltage of the TPS5401 is done easily by using equation 10 below.

$$R7 = R8 \times \frac{V_{OUT} - 0.8V}{0.8V} \quad (10)$$

For higher efficiency, larger values for  $R8$  and  $R7$  are desired. However, if too high of resistors are selected the converter can be vulnerable to noise. Limit the max  $R8$  and  $R7$  to be 775k $\Omega$ . Assume 100k $\Omega$  for  $R8$ , and  $R7$  is calculated at 316k $\Omega$ . The output will still read 3.3V after the 4kV surge test.

## Duty Cycle and Frequency Set Resistor

The switching frequency ( $F_{sw}$ ) is adjustable over a wide range for the TPS5401. To balance efficiency and size, a switching frequency must be chosen that meets the minimum on time requirements of the converter, the short circuit protection requirements, and also results in a reasonable value for the inductor. The minimum controllable on time for the TPS5401 is typically 120ns. See the "Selecting the Switching Frequency" section of the TPS5401 datasheet for more details on the frequency shift. By choosing a  $F_{sw}$  of 365kHz, all conditions for meeting the current limit protections and minimum on time are met.

## Inductor

To determine the inductor value, calculate the average inductor current at the minimum and maximum output currents and minimum and maximum input voltages. Assuming a 41V  $V_{INMAX}$ , 37V  $V_{INMIN}$ , 3mA  $I_{OMIN}$ , and 50mA  $I_{OMAX}$ , the minimum and maximum inductance for the application can be calculated using equations 11 and 12.

$$L_{ONMIN} = \frac{(V_{INMIN} - V_O) \times V_O}{2 \times V_{INMIN} \times f_{sw} \times I_{OMAX}} \quad (11)$$

$$L_{ONMAX} = \frac{f_{sw} \times (V_{INMAX} - V_O) \times V_{INMAX} \times t_{ONMIN}^2}{2 \times V_O \times I_{OMIN}} \quad (12)$$

Using a  $V_{INMAX}$  of 41V,  $V_{INMIN}$  of 37V,  $V_{OUT}$  of 3.3V,  $I_{OMAX}$  of 50mA,  $I_{OMIN}$  of 3mA, and  $F_{sw}$  of 365kHz, a minimum inductor value of 82.3 $\mu$ H and a maximum inductor value of 410 $\mu$ H is calculated. Choosing an inductor closest to the minimum, results in an 82 $\mu$ H inductor with an  $R_{DC}$  of 261 $\Omega$ . Use equations 13 through 16 to verify that  $D1 + D2$  is less than 1; otherwise, in DCM operation, and inductor is rated up and beyond  $I_{LRMS}$  and  $I_{LPEAK}$ .

$$I_{LPEAK} = \sqrt{\frac{2 \times V_O \times I_{OMAX} \times (V_{INMAX} - V_O)}{V_{INMAX} \times L_O \times f_{sw}}} \quad (13)$$

$$D1 = \sqrt{\frac{2 \times V_O \times I_O \times L_O \times f_{sw}}{V_{IN} \times (V_{IN} - V_O)}} \quad (14)$$

$$D2 = \left( \frac{V_{IN} - V_O}{V_O} \right) \times D1 \quad (15)$$

$$I_{LRMS} = I_{LPEAK} \times \sqrt{\frac{D1 + D2}{3}} \quad (16)$$

## Output Capacitor

The output capacitance is chosen to handle the expected load step requirements of the load. Since the e-meter application is not demanding, a load step of less than 50mA can be expected. This will result in a lower capacitance than if a large load step is required, as the output cap maintains the output voltage during the load step. The  $C_{OUT}$  should be sized by meeting the most demanding of equations 17, 18, and 19.

$$C_O \geq \frac{I_{LPEAK} \times (D1 + D2)}{V_{ORIPPLE} \times f_{sw} \times 8} \quad (17)$$

$$C_O \geq L_O \times \frac{I_O^2}{(V_O + \Delta V)^2 - V_O^2} \quad (18)$$

$$C_O \geq L_O \times \frac{I_O}{\Delta V - f_{CO}} \quad (19)$$

The most stringent of these is equation 17, which results in a requirement of 1.04 $\mu$ F. The capacitor standard size is chosen to be 22 $\mu$ F. Keep in mind that ceramic capacitors have a reduction in capacitance based on the bias of the output voltage, so using a larger value than calculated is advised. The output capacitor also provides the pole for the Type II compensation, so to accurately predict the crossover; it is required to de-rate the output capacitance based on the output voltage and capacitor voltage rating.

## Diode Selection

The diode must have a reverse voltage rating equal to or greater than  $V_{INMAX}$ . The peak current rating of the diode must be greater than the maximum inductor current. The diode should also have a low forward voltage. For this design example, the B150-E3 Schottky diode with 50V reverse voltage is selected for its lower forward voltage of 0.75V.

## Compensation and Frequency Response

To stabilize the closed-loop circuit, a compensation network is required. Because the TPS5401 is a current mode converter, the compensation can be Type IIA, which consists of a resistor and capacitor in parallel with another capacitor on the COMP pin.

The first step is to determine the  $K_{dcm}$ , DCM gain, and the  $F_m$ , modulator gain. These can be calculated using equations 20 and 21.

$$K_{dcm} = \frac{2 \times V_{OUT} \times (V_{IN} - V_{OUT})}{D1 \times V_{IN} \times \left( 2 + \frac{R_{dc} \times I_{OUT}}{V_{OUT}} \right) - V_{OUT}} \quad (20)$$

$$F_m = \frac{g_{mps}}{\left[ \frac{V_{IN} - V_O}{L_O \times f_{sw}} \right] + .805} \quad (21)$$

Since,  $g_{mps} = 1.9$  and  $R_{DC}$  (DCR of  $L_O$ ) = .261 $\Omega$ ,  $K_{dcm} = 37.37$  and  $F_m = .951$ .

Next, determine the power stage pole and zero frequencies. These can be calculated using equations 22 and 23.

$$f_{pmod} = \frac{I_{OMAX}}{2 \times \pi \times V_{OUT} \times C_{OUT}} \times \frac{\left( 2 - \frac{V_{OUT}}{V_{IN}} \right)}{\left( 1 - \frac{V_{OUT}}{V_{IN}} \right)} \quad (22)$$

$$f_{zmod} = \frac{1}{2 \times \pi \times Resr \times C_{OUT}} \quad (23)$$

For  $C_{OUT}$ , the derated value of  $18.3\mu\text{F}$  is used. In this case,  $f_{pmod} = 276\text{Hz}$ , and  $f_{zmod} = 2.91\text{MHz}$ . Then, determine the geometric mean of the modulator pole and the ESR zero (equation 24), and the mean of the modulator pole and the switching frequency (equation 25).

$$f_{co} = \sqrt{f_{pmod} \times f_{zmod}} \quad (24)$$

$$f_{co2} = \sqrt{f_{sw} \times f_{pmod}} \quad (25)$$

In this case,  $f_{co1} = 28.3\text{ kHz}$ , and  $f_{co2} = 10\text{ kHz}$ . Choose the smaller of the two as a starting point for the crossover frequency. The target crossover frequency chosen is  $10\text{ kHz}$ .

Finally, calculate the compensation pole (resistor), use equation 26. To calculate the compensation zero (capacitor), use equation 27.

$$R5 = \frac{f_{co2} \times V_{OUT}}{K_{dcm} \times F_m \times f_{pmod} \times g_{ema} \times V_{REF}} \quad (26)$$

$$C6 = \frac{1}{2 \times \pi \times R5 \times K_{dcm} \times F_m} \quad (27)$$

In this case,  $R5 = 43.3\text{k}\Omega$ , and  $C6 = .1\mu\text{F}$ . The nearest standard values for  $R5$  and  $C6$  are  $43.2\text{k}\Omega$  and  $.1\mu\text{F}$ , so these are used. Using equations 28 and 29, the  $C_{pole}$  or  $C7$  in this circuit, may be calculated. Use the larger of the two calculated values.

$$C_{pole1} = \frac{C_{OUT} \times R_{esr}}{R5} \quad (28)$$

$$C_{pole2} = \frac{1}{R5 \times f_{sw} \times \pi} \quad (29)$$

In this case, the calculated values are  $1.27\text{pF}$  and  $20.2\text{pF}$ . In this case, a standard value of  $18\text{pF}$  was chosen. The resulting bode plot is shown in the results section of the application note.

## Input Capacitors

The TPS5401 requires a high quality ceramic, type X5R or X7R, input decoupling capacitor of at least  $3\mu\text{F}$ , and in some cases a bulk capacitance. The voltage rating of the input capacitor must be greater than the maximum input voltage. The capacitor must also have a ripple current rating greater than the maximum input current ripple of the TPS5401, which can be calculated using equation 30.

$$I_{C_{RMS}} = I_{L_{PEAK}} \sqrt{\left(\frac{D1}{3} - \left(\frac{D1}{4}\right)^2\right)} \quad (30)$$

In this case, two  $2.2\mu\text{F}/50\text{V}$  capacitors in parallel are selected. These capacitors must be placed as close as possible to the input pin of the switching power device.



## Slow Start Time

The slow start capacitor determines the minimum amount of time it will take for the output voltage to reach its nominal programmed value during power up. The slow start time must be long enough to allow the regulator to charge the output capacitor up to the output voltage without drawing excessive current. Equation 31 can be used to find the minimum slow start time,  $t_{ss}$ , necessary to charge the output capacitor,  $C_{OUT}$ , from 10% to 90% of the output voltage with an average slow start current  $I_{SSavg}$ . In the example, to charge the 22 $\mu$ F output capacitor up to 3.3V while only allowing the average input current to be 5mA would require at least 11.6ms slow start time.

$$t_{ss} > \frac{C_{OUT} \times V_{OUT} \times 0.8}{I_{SSavg}} \quad (31)$$

Once the slow start time is known, the slow start capacitor value can be found with equation 32.

$$C_{ss}(nF) = \frac{t_{ss}(ms) \times I_{SS}(\mu A)}{V_{REF}(V) \times 0.8} \quad (32)$$

In this case, to achieve a 12 ms minimum slow start time,  $I_{ss}$  of 2 $\mu$ A, and  $V_{REF}$  of 0.8V, a 0.047  $\mu$ F capacitor is chosen.

## Power Dissipation

In order to measure power dissipation from the AC line, a power meter must be used. Measure the real power in as  $P_{inM}$ . The  $P_D$ , total power dissipation, is calculated in equation 33.

$$P_D = \text{real}(P_{inM}) - I_{OUT} \times V_{OUT} \quad (33)$$

At  $I_{OUT} = 40\text{mA}$ ,  $V_{OUT} = 3.291$ , and measured real  $P_{in} = 454.4\text{mW}$ ,  $P_D = 322.8\text{mW}$ . For a theoretical power dissipation calculation, equations 34 – 47 will provide a rough estimate.

$$P_{Dcal} = P_{fet} + P_{d1} = P_{driver} + P_{controller} + P_{uvlo} + P_{d2} \text{ and } 3 + P_{rin} + P_{cap} + P_{ind} \quad (34)$$

## FET

$$I_{fet} = \sqrt{D1 \times \left( I_{OUT}^2 + \frac{I_{LPEAK}^2}{12} \right)} \quad (35)$$

$$P_{fet_{cond}} = I_{fet}^2 \times R_{DS(on)} \quad (36)$$

$$P_{fet_{sw}} = \frac{1}{4} \times f_{sw} \times \text{switch}_{time} \times V_{INMAX} \times \left( I_{OUT} + \frac{I_{LPEAK}}{2} \right) \quad (37)$$

$$P_{fet} = P_{fet_{sw}} + P_{fet_{cond}} \quad (38)$$

Assuming  $I_{OUT} = 40\text{mA}$ ,  $R_{DS(on)} = .2\Omega$ ,  $I_{peak}$  and  $D1$  equal values calculated before,  $I_{fet} = 14.3\text{mA}$  and  $P_{fet_{cond}} = 41.1\mu\text{W}$ . With  $f_{sw} = 365\text{kHz}$ ,  $switch\_time = 10\text{ns}$ ,  $V_{INMAX} = 41\text{V}$ ,  $P_{fet_{sw}}$  is calculated to be  $3.37\text{mW}$  and the resultant  $P_{fet}$  totals to be  $3.41\text{mW}$ .

### Internal IC

$$P_{driver} = f_{sw} \times V_{drive} \times Q_{gfet} \quad (39)$$

$$P_{controller} = I_{non-sw} \times V_{IN} \quad (40)$$

Assuming  $V_{drive} = 6\text{V}$ ,  $Q_{gfet} = 15\text{nC}$ , and  $I_{non-sw} = 116\mu\text{A}$ ,  $P_{driver} = 32.85\text{mW}$  and  $P_{controller} = 4.5\text{mW}$ .

### Pre-Converter

$$P_{d1 \text{ and } 2} = P_{IN} - \frac{V_{OUT} \times I_{OUT}}{\eta} \quad (41)$$

Since,  $V_{OUT} = 3.3\text{V}$  and  $I_{OUT} = 40\text{mA}$  we can assume for this analysis,  $\eta \approx 57\%$ . Using the value calculated earlier in this application note for  $P_{in}$ ,  $272.8\text{mW}$ ,  $P_{d2 \text{ and } 3} = 32.8\text{mW}$ . Power dissipation in input resistance and cap drop should be done using the RMS current. RMS current will be approximately full wave rectifier current, given in equation 33.

$$I_{IN \text{ frms}} = V_{RMS} \times 2 \times \pi \times 50\text{Hz} \times C_{ap} \quad (42)$$

$$P_{rin} = I_{IN \text{ frms}}^2 \times R_{in} \quad (43)$$

$$P_{cap} = I_{IN \text{ frms}}^2 \times R_{cap} \quad (44)$$

$I_{IN \text{ frms}}$  calculates to  $15.9\text{mA}$  so, the  $560\Omega$  resistor will dissipate  $141.57\text{mW}$  of power. Estimating  $R_{cap} \sim 50\Omega$ , results is  $P_{cap}$  dissipation of  $12.64\text{mW}$ .

### Low Side Catch Diode and Inductor

During the converter on time, the output current is provided by the internal switching FET. During the off time, the output current flows through the catch diode. The average power in the diode is given by equation 20.

$$P_{d3} = \sqrt{\frac{2 \times I_O \times L_O \times f_{sw}}{V_{IN}^2 \times V_O - V_O^2 \times V_{IN}}} \left( V_{INMAX} - V_{OUT} \right) \times I_{OUT} \times V_{fd} + \frac{C_j \times f_{sw} \times \left( V_{IN} + V_{fd} \right)^2}{2} \quad (45)$$

The selected diode will dissipate  $69.1\text{mW}$  assuming a  $40\text{mA}$  output current, diode junction capacitance of  $150\text{pF}$ ,  $V_{fd}$  of  $0.75\text{V}$ ,  $f_{sw}$  of  $365\text{kHz}$  and  $V_{INMAX}$  of  $41\text{V}$ . Power dissipated through the inductor is calculated below in equation 46.

$$P_{IND} = I_{OUT}^2 \times R_{DC} + I_{NDcorelosses} \quad (46)$$

Inductor core losses were calculated from the manufacturer to be about  $8\text{mW}$  bring the total power dissipated through the inductor to  $\sim 9\text{mW}$ .

### ***Input of Converter***

The UVLO resistors are the only components on the converter's input dissipating enough power to consider in this analysis. The power dissipated through the UVLO resistors is calculated using equation 10.

$$P_{UVLO} = \frac{V_{IN}^2}{R2 + R3} \quad (47)$$

Calculated power dissipated totals to a value of 306.1 mW.

## Appendix A. Experimental Results

All results are to be assumed at 3.3V output, 40mA load, and 230VAC input unless specified otherwise.

### A.1 Efficiency

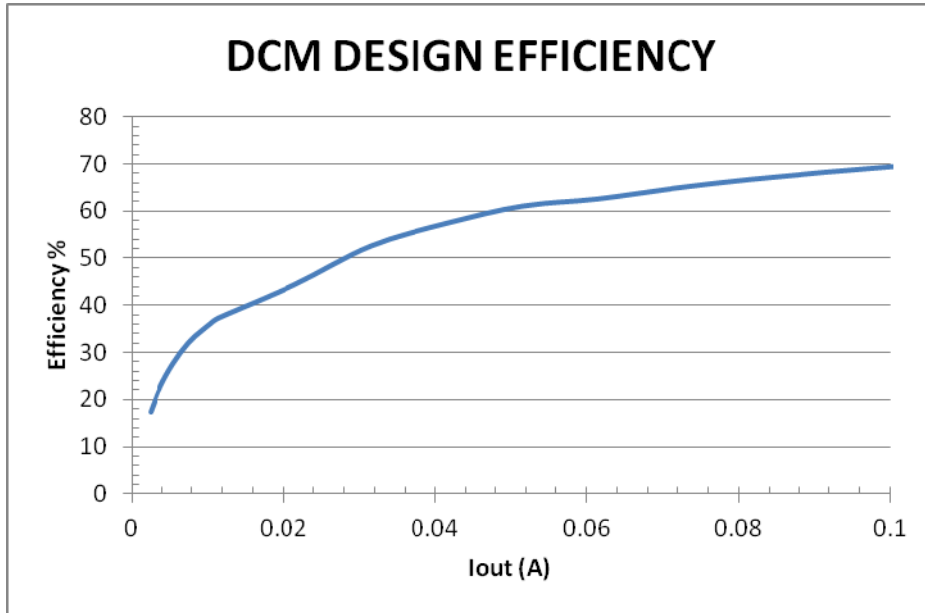


Figure A-1. DCM Design Efficiency

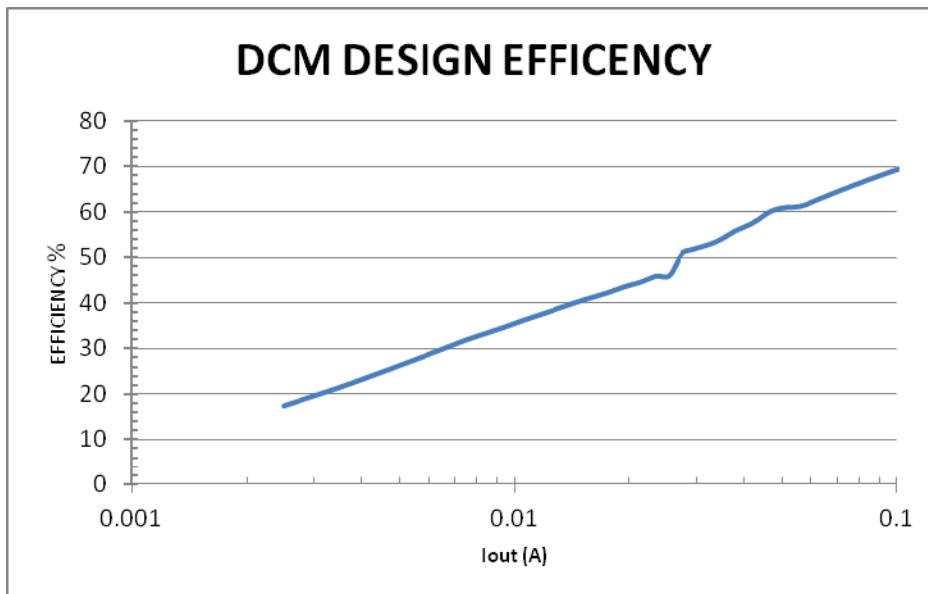
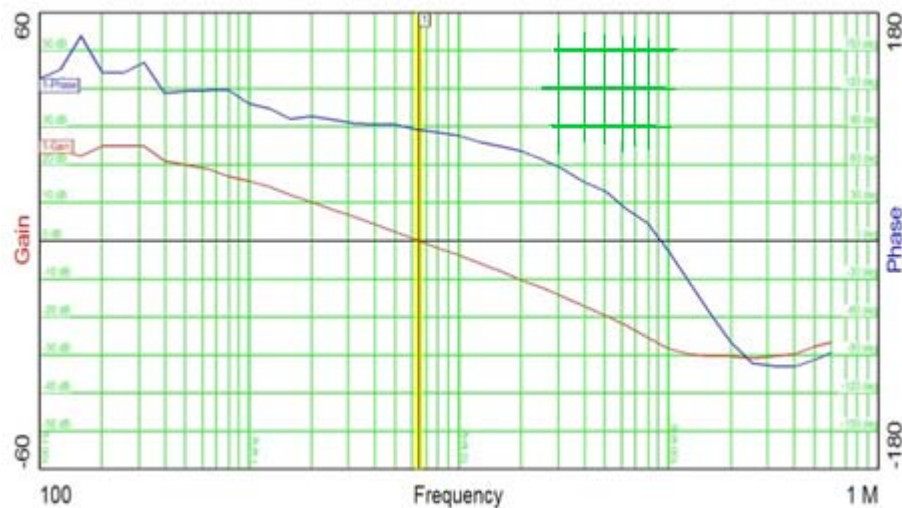


Figure A-2. Logarithmic DCM Design Efficiency

## A.2 Control Loop



**Figure A-3. Frequency Response at 40mA Load**

The de-rated value of the capacitor was smaller than the value used by  $3.5\mu\text{F}$ . However, it is doubtful that this would cause the variation of the graph between theoretical and actual data. The target crossover frequency is also smaller. The graph shows 6.5kHz, when 10kHz was the target. Most of the variation between the actual and theoretical data is due to the fact that when a simulated graph is produced it has ideal conditions and when the data is actually found in the lab, it can have some variation.

V<sub>OUT</sub> Regulation

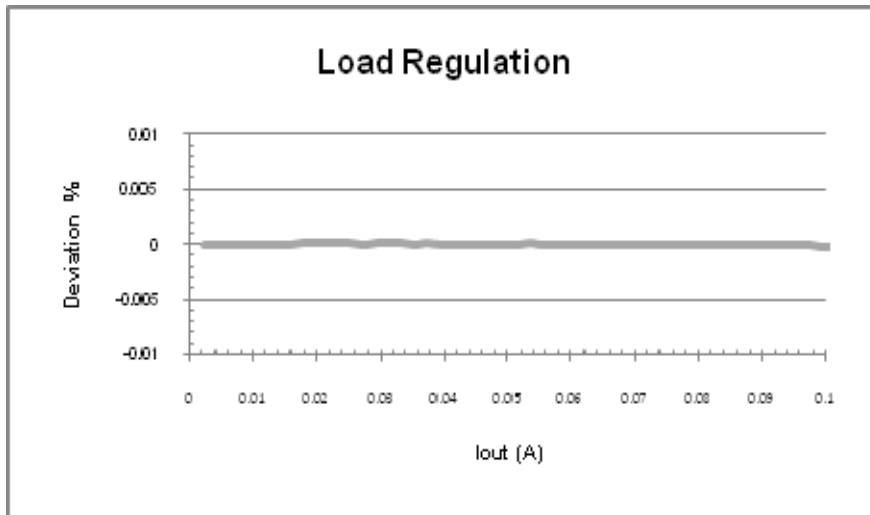


Figure A-4. Load Regulation at 3.3V<sub>OUT</sub>.

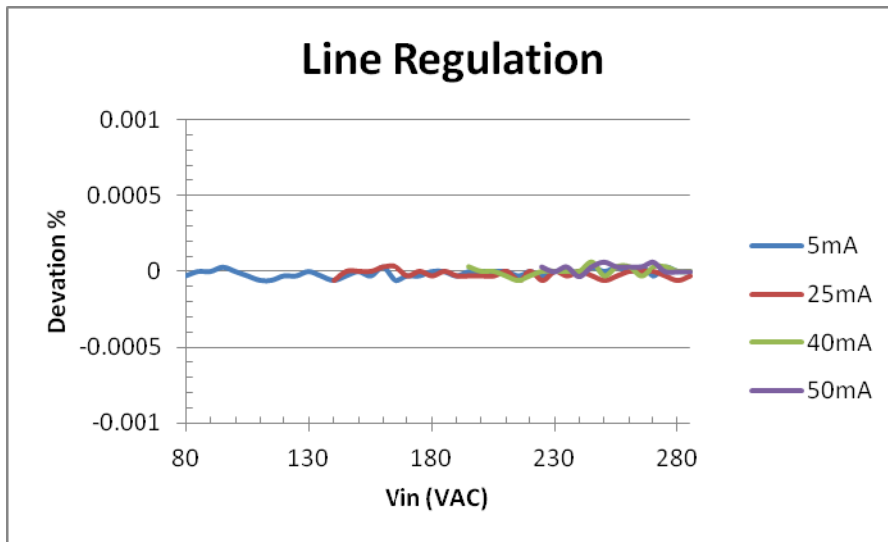


Figure A-5. Line Regulation at 3.3V<sub>OUT</sub>.

### A.3 $V_{IN}$ Ripple

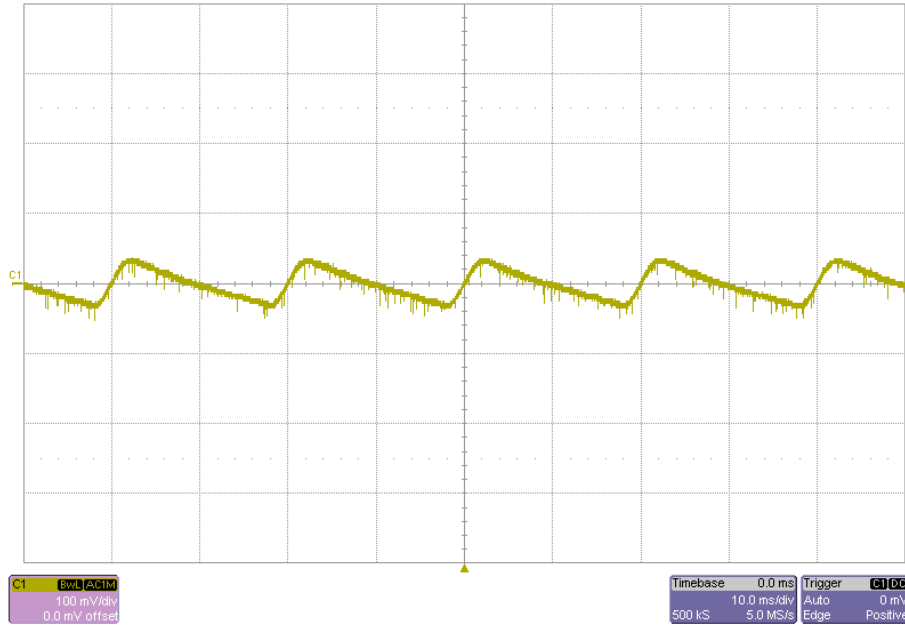


Figure A-6.  $V_{IN}$  Ripple at 5mA Load

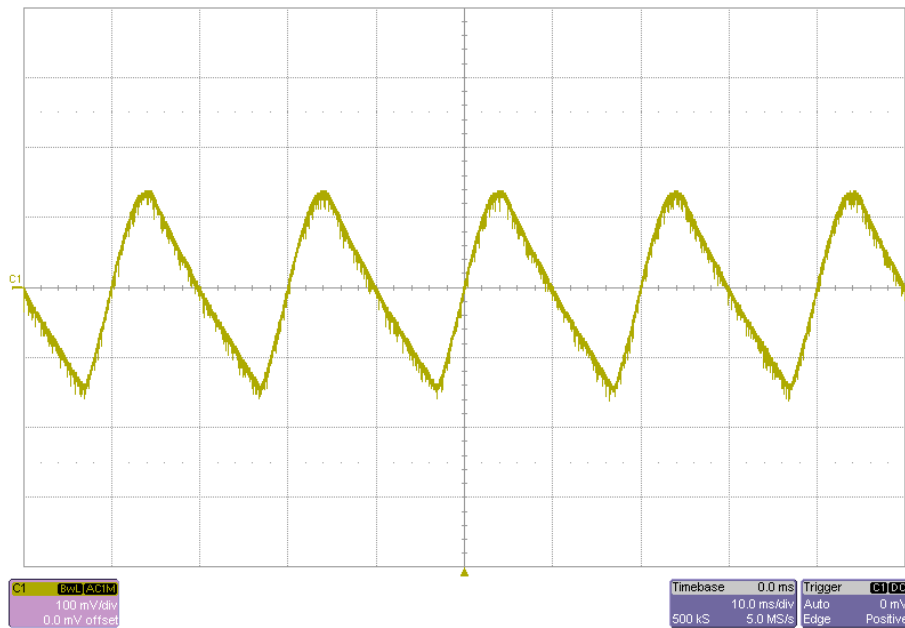


Figure A-7.  $V_{IN}$  Ripple at 40mA Load

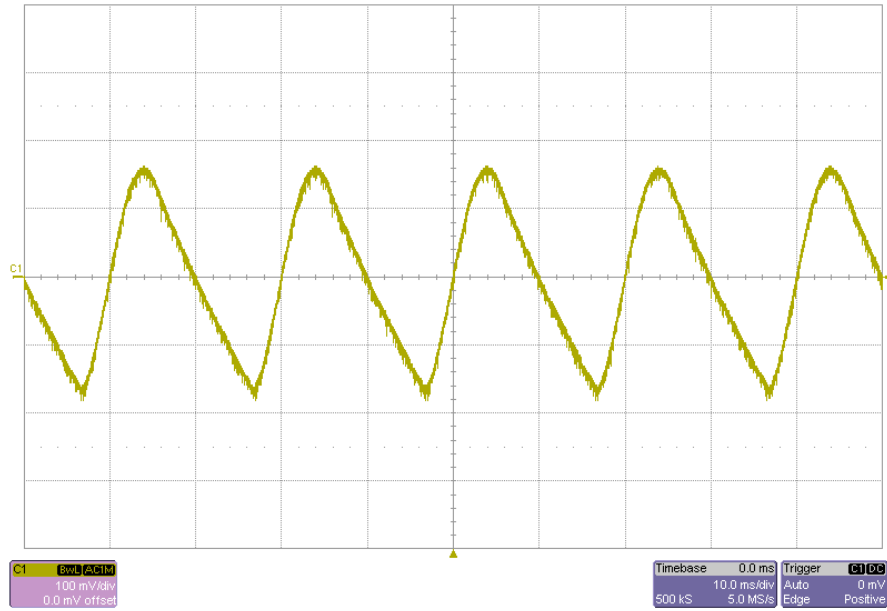


Figure A-8.  $V_{IN}$  Ripple at 50mA Load

#### A.4 $V_{OUT}$ Ripple

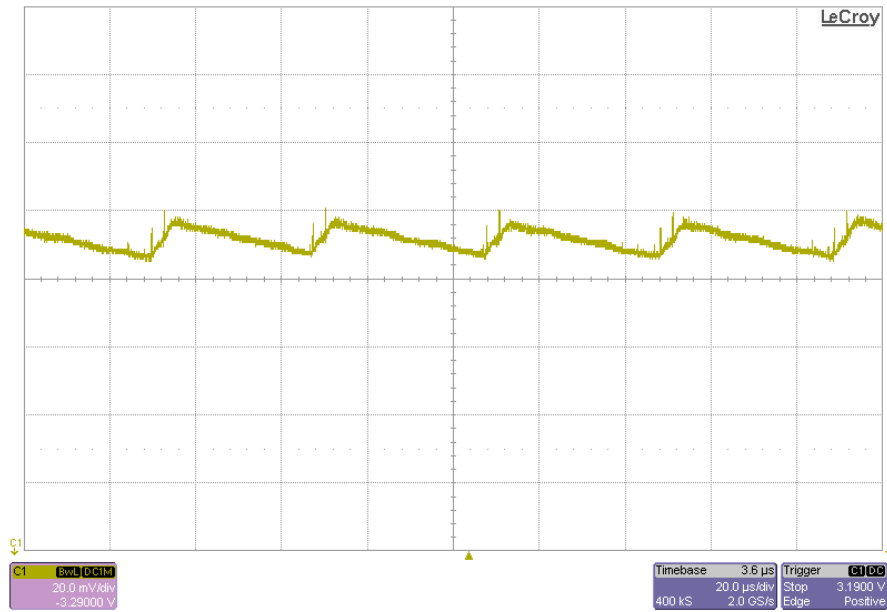


Figure A-9.  $V_{OUT}$  Ripple at 5mA



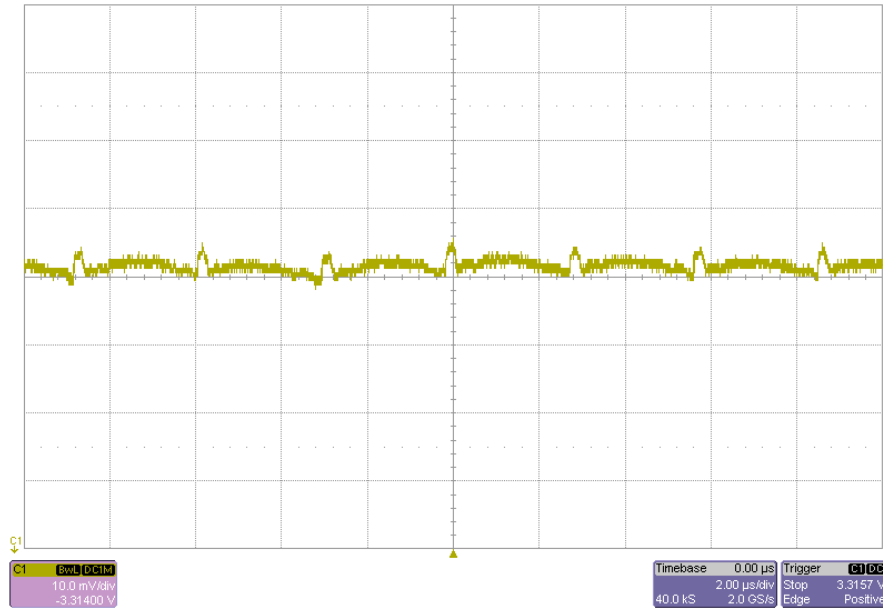


Figure A-10.  $V_{OUT}$  Ripple at 40mA

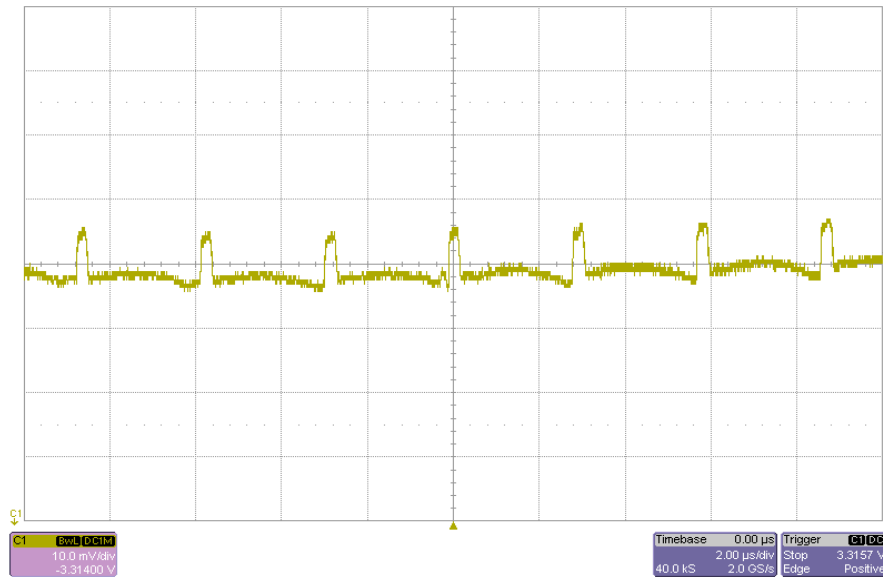


Figure A-11.  $V_{OUT}$  Ripple at 50mA

### A.5 Slow-Start

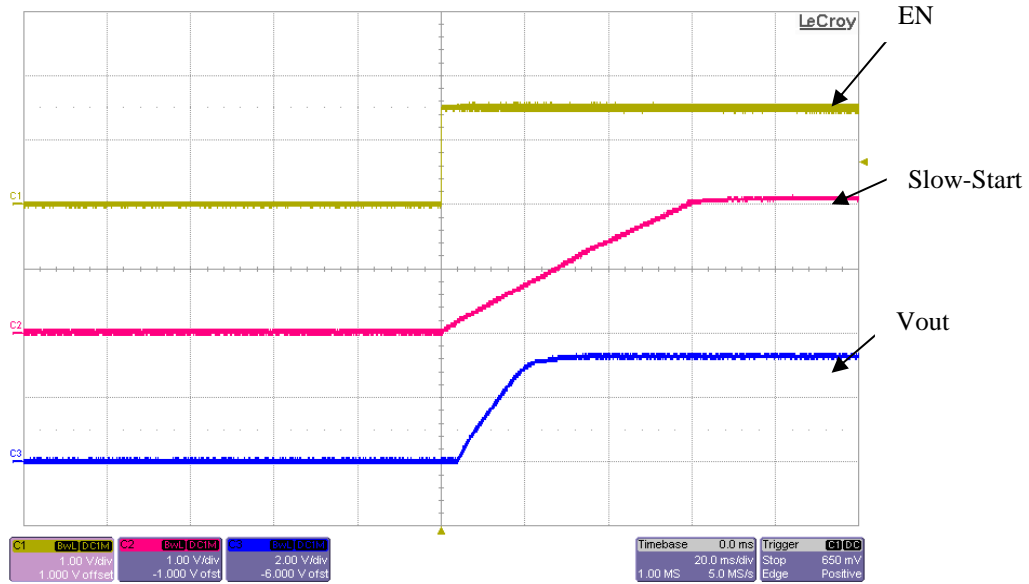


Figure A-12. Slow-Start vs. EN

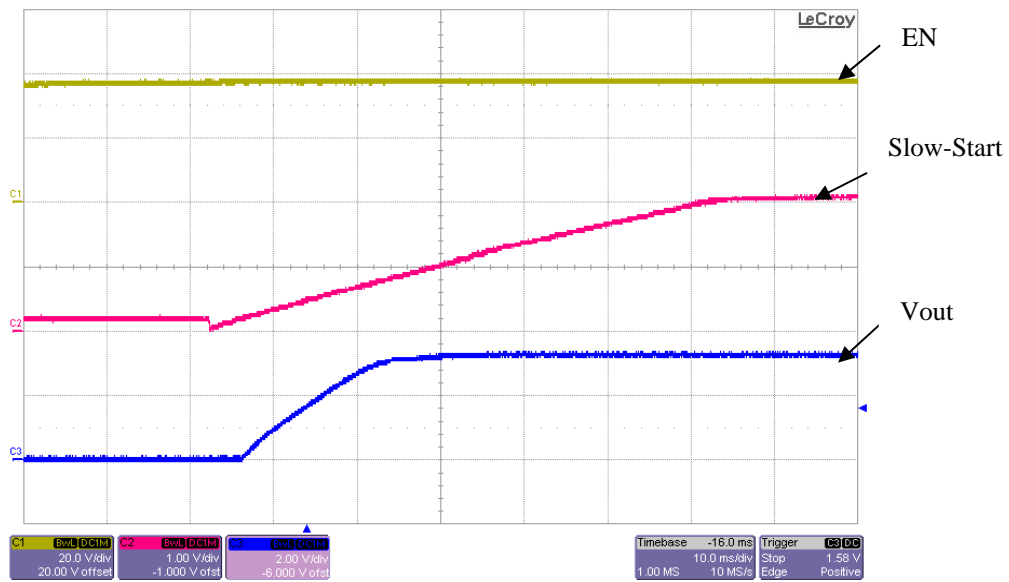


Figure A-13. Slow-Start vs.  $V_{IN}$

### A.6 Surge Test

The reference circuit was tested for line surges using the 4kV IEC-61000-4-5 standard and it passed. All functions work properly after testing. Also note that there was no Metal Oxide Varistor (MOV) at the input.

## IMPORTANT NOTICE

Texas Instruments Incorporated and its subsidiaries (TI) reserve the right to make corrections, modifications, enhancements, improvements, and other changes to its products and services at any time and to discontinue any product or service without notice. Customers should obtain the latest relevant information before placing orders and should verify that such information is current and complete. All products are sold subject to TI's terms and conditions of sale supplied at the time of order acknowledgment.

TI warrants performance of its hardware products to the specifications applicable at the time of sale in accordance with TI's standard warranty. Testing and other quality control techniques are used to the extent TI deems necessary to support this warranty. Except where mandated by government requirements, testing of all parameters of each product is not necessarily performed.

TI assumes no liability for applications assistance or customer product design. Customers are responsible for their products and applications using TI components. To minimize the risks associated with customer products and applications, customers should provide adequate design and operating safeguards.

TI does not warrant or represent that any license, either express or implied, is granted under any TI patent right, copyright, mask work right, or other TI intellectual property right relating to any combination, machine, or process in which TI products or services are used. Information published by TI regarding third-party products or services does not constitute a license from TI to use such products or services or a warranty or endorsement thereof. Use of such information may require a license from a third party under the patents or other intellectual property of the third party, or a license from TI under the patents or other intellectual property of TI.

Reproduction of TI information in TI data books or data sheets is permissible only if reproduction is without alteration and is accompanied by all associated warranties, conditions, limitations, and notices. Reproduction of this information with alteration is an unfair and deceptive business practice. TI is not responsible or liable for such altered documentation. Information of third parties may be subject to additional restrictions.

Resale of TI products or services with statements different from or beyond the parameters stated by TI for that product or service voids all express and any implied warranties for the associated TI product or service and is an unfair and deceptive business practice. TI is not responsible or liable for any such statements.

TI products are not authorized for use in safety-critical applications (such as life support) where a failure of the TI product would reasonably be expected to cause severe personal injury or death, unless officers of the parties have executed an agreement specifically governing such use. Buyers represent that they have all necessary expertise in the safety and regulatory ramifications of their applications, and acknowledge and agree that they are solely responsible for all legal, regulatory and safety-related requirements concerning their products and any use of TI products in such safety-critical applications, notwithstanding any applications-related information or support that may be provided by TI. Further, Buyers must fully indemnify TI and its representatives against any damages arising out of the use of TI products in such safety-critical applications.

TI products are neither designed nor intended for use in military/aerospace applications or environments unless the TI products are specifically designated by TI as military-grade or "enhanced plastic." Only products designated by TI as military-grade meet military specifications. Buyers acknowledge and agree that any such use of TI products which TI has not designated as military-grade is solely at the Buyer's risk, and that they are solely responsible for compliance with all legal and regulatory requirements in connection with such use.

TI products are neither designed nor intended for use in automotive applications or environments unless the specific TI products are designated by TI as compliant with ISO/TS 16949 requirements. Buyers acknowledge and agree that, if they use any non-designated products in automotive applications, TI will not be responsible for any failure to meet such requirements.

Following are URLs where you can obtain information on other Texas Instruments products and application solutions:

### Products

Audio	<a href="http://www.ti.com/audio">www.ti.com/audio</a>
Amplifiers	<a href="http://amplifier.ti.com">amplifier.ti.com</a>
Data Converters	<a href="http://dataconverter.ti.com">dataconverter.ti.com</a>
DLP® Products	<a href="http://www.dlp.com">www.dlp.com</a>
DSP	<a href="http://dsp.ti.com">dsp.ti.com</a>
Clocks and Timers	<a href="http://www.ti.com/clocks">www.ti.com/clocks</a>
Interface	<a href="http://interface.ti.com">interface.ti.com</a>
Logic	<a href="http://logic.ti.com">logic.ti.com</a>
Power Mgmt	<a href="http://power.ti.com">power.ti.com</a>
Microcontrollers	<a href="http://microcontroller.ti.com">microcontroller.ti.com</a>
RFID	<a href="http://www.ti-rfid.com">www.ti-rfid.com</a>
OMAP Mobile Processors	<a href="http://www.ti.com/omap">www.ti.com/omap</a>
Wireless Connectivity	<a href="http://www.ti.com/wirelessconnectivity">www.ti.com/wirelessconnectivity</a>

### Applications

Automotive and Transportation	<a href="http://www.ti.com/automotive">www.ti.com/automotive</a>
Communications and Telecom	<a href="http://www.ti.com/communications">www.ti.com/communications</a>
Computers and Peripherals	<a href="http://www.ti.com/computers">www.ti.com/computers</a>
Consumer Electronics	<a href="http://www.ti.com/consumer-apps">www.ti.com/consumer-apps</a>
Energy and Lighting	<a href="http://www.ti.com/energy">www.ti.com/energy</a>
Industrial	<a href="http://www.ti.com/industrial">www.ti.com/industrial</a>
Medical	<a href="http://www.ti.com/medical">www.ti.com/medical</a>
Security	<a href="http://www.ti.com/security">www.ti.com/security</a>
Space, Avionics and Defense	<a href="http://www.ti.com/space-avionics-defense">www.ti.com/space-avionics-defense</a>
Video and Imaging	<a href="http://www.ti.com/video">www.ti.com/video</a>

TI E2E Community Home Page

[e2e.ti.com](http://e2e.ti.com)

Mailing Address: Texas Instruments, Post Office Box 655303, Dallas, Texas 75265  
Copyright © 2012, Texas Instruments Incorporated