

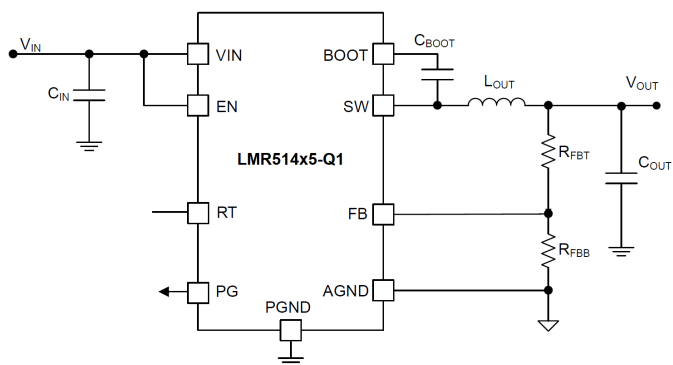
# LMR514x5-Q1 36V, 2.5A / 3.5A, Automotive, Synchronous Buck Converter With Low $I_Q$

## 1 Features

- AEC-Q100 qualified for automotive applications
  - Device temperature grade 1:  $-40^{\circ}\text{C}$  to  $+125^{\circ}\text{C}$  ambient operating temperature
- **Functional Safety-Capable**
  - [Documentation available to aid functional safety system design](#)
- Supports automotive system requirements:
  - Wide input voltage range: 4V to 36V
  - Continuous output current: 2.5A or 3.5A
  - $\pm 1.0\%$  tolerance voltage reference at room temperature
  - Minimum switching-on time: 75ns (typical)
  - Low quiescent current: 25 $\mu\text{A}$
  - Adjustable frequency: 200kHz to 1MHz
  - Frequency spread spectrum
  - Protection features:
    - Precision enable input
    - Open-drain PGOOD
    - $V_{\text{IN}}$  undervoltage lockout (UVLO)
    - Cycle-by-cycle current limiting
    - Short-circuit protection with hiccup mode
    - Thermal shutdown
- Small design size and ease of use
  - Integrated synchronous rectification
  - Internal compensation for ease of use
  - WSON-12 package
- PFM and FPWM options in pin-to-pin compatible package
- Create a custom design using the LMR514x5-Q1 with the [WEBENCH® Power Designer](#)

## 2 Applications

- [Automotive ADAS](#) and [body electronics](#)
- [Automotive infotainment and cluster: head unit, media hub, USB charge, display](#)



**Simplified Schematic**

## 3 Description

The LMR514x5-Q1 is a wide- $V_{\text{IN}}$ , easy-to-use, synchronous buck converter capable of driving up to 2.5A or 3.5A load current. With a wide input range of 4V to 36V, the device is designed for a wide range of industrial applications for power conditioning from an unregulated source.

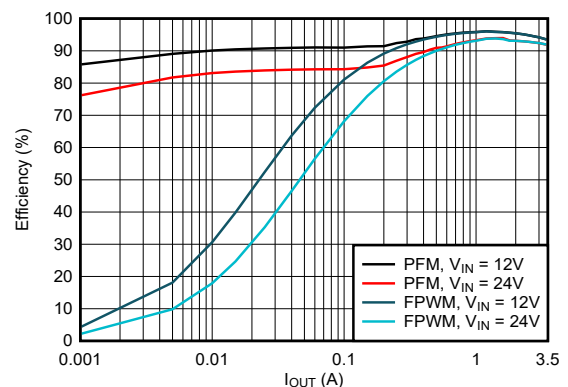
The LMR514x5-Q1 features adjustable switching frequency from 200kHz to 1MHz with an external resistor, which provides the flexibility to optimize either efficiency or external component size. The device has pulse frequency modulation ([PFM version](#)) to realize high efficiency at light load, and forced pulse width modulation ([FPWM version](#)) to achieve constant frequency, and small output voltage ripple over the full load range. Soft-start and compensation circuits are implemented internally, which allows the device to be used with minimum external components.

The device has built-in protection features, such as cycle-by-cycle current limit, hiccup mode short-circuit protection, and thermal shutdown in case of excessive power dissipation. The LMR514x5-Q1 is available in a WSON-12 package.

### Device Information

PART NUMBER <sup>(1)</sup>	CURRENT	PACKAGE <sup>(2)</sup>	BODY SIZE (NOM)
LMR51425-Q1	2.5A	DRR (WSON, 12)	3.00mm × 3.00mm
LMR51435-Q1	3.5A		

- (1) See the [Device Comparison Table](#).
- (2) For more information, see [Section 11](#).



**Efficiency vs Output Current  $V_{\text{OUT}} = 5\text{V}$ , 440kHz**



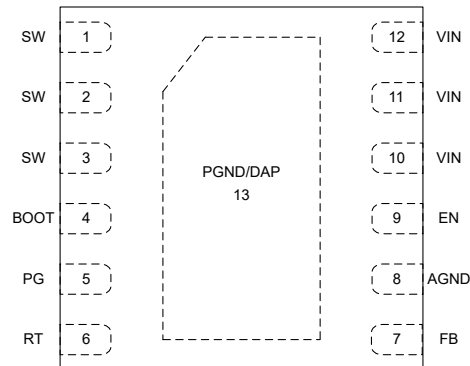
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## 4 Device Comparison Table

ORDERABLE PART NUMBER	Current	PFM OR FPWM	Spread Spectrum
LMR51435SQDRRRQ1	3.5A	PFM	Yes
LMR51435FSQDRRRQ1	3.5A	FPWM	Yes
LMR51425SQDRRRQ1	2.5A	PFM	Yes
LMR51425FSQDRRRQ1	2.5A	FPWM	Yes

## 5 Pin Configuration and Functions



**Figure 5-1. 12-Pin WSON DRR Package (Top View)**

**Table 5-1. Pin Functions**

PIN		TYPE <sup>(1)</sup>	DESCRIPTION
NAME	NO		
SW	1, 2, 3	P	Switching output of the converter. Internally connected to source of the high-side FET and drain of the low-side FET. Connect to power inductor.
BOOT	4	P	Bootstrap capacitor connection for high-side FET driver. Connect a high quality 100nF capacitor from this pin to the SW pin.
PG	5	A	Open-drain power-good monitor output that asserts low if the FB voltage is not within the specified window thresholds. A 10kΩ to 100kΩ pull up resistor to a suitable voltage is required. If not used, PG can be left open or connected to GND.
RT	6	A	Frequency setting pin used to set the switching frequency between 200kHz and 1MHz by placing an external resistor from RT to AGND. RT open defaults to 440kHz and RT short to ground defaults to 1MHz.
FB	7	A	Feedback input to the converter. Connect a resistor divider to set the output voltage. Never short this terminal to ground during operation.
AGND	8	G	Analog ground. Zero-voltage reference for internal references and logic. All electrical parameters are measured with respect to this pin. These pins must be connected to PGND using a small net-tie.
EN	9	A	Precision enable input pin. High = On, Low = Off. Can be connected to VIN. Precision enable allows the pin to be used as an adjustable input voltage UVLO. Connect an external resistor divider between this pin, VIN and AGND to create an external UVLO. <i>Do not float.</i>
VIN	10, 11, 12	P	Input supply voltage. Connect the input supply to these pins. Connect input capacitors CIN between these pins and PGND in close proximity to the device.
PGND	13	G	Power ground terminals, connected to the source of low-side FET internally. Connect to system ground, ground side of CIN and COUT. Path to CIN must be as short as possible.

(1) A = Analog, P = Power, G = Ground.

## 6 Specifications

### 6.1 Absolute Maximum Ratings

Over junction temperature range of  $-40^{\circ}\text{C}$  to  $150^{\circ}\text{C}$  (unless otherwise noted)<sup>(1)</sup>

		MIN	MAX	UNIT
Input voltage	VIN to PGND	-0.3	38	V
	EN to PGND	-0.3	$V_{IN} + 0.3$	V
	FB to PGND	-0.3	5.5	V
	RT to PGND	-0.3	5.5	V
Output voltage	BOOT to SW	-0.3	5.5	V
	SW to PGND	-0.3	38	V
	SW to PGND less than 10ns transients	-4.5	40	V
	PG to PGND	-0.3	20	V
Junction Temperature $T_J$		-40	150	$^{\circ}\text{C}$
Storage temperature, $T_{stg}$		-65	150	$^{\circ}\text{C}$

- (1) Operation outside the Absolute Maximum Ratings may cause permanent device damage. Absolute Maximum Ratings do not imply functional operation of the device at these or any other conditions beyond those listed under Recommended Operating Conditions. If used outside the Recommended Operating Conditions but within the Absolute Maximum Ratings, the device may not be fully functional, and this may affect device reliability, functionality, performance, and shorten the device lifetime.

### 6.2 ESD Ratings

			VALUE	UNIT
$V_{(ESD)}$	Electrostatic discharge	Human body model (HBM), per AEC Q100-002 <sup>(1)</sup>	$\pm 2000$	V
		Charged device model (CDM), per AEC Q100-011	$\pm 750$	

- (1) AEC Q100-002 indicates that HBM stressing must be in accordance with the ANSI/ESDA/JEDEC JS-001 specification.

### 6.3 Recommended Operating Conditions

Over the recommended operating junction temperature range of  $-40^{\circ}\text{C}$  to  $150^{\circ}\text{C}$  (unless otherwise noted)<sup>(1)</sup>

		MIN	NOM	MAX	UNIT
Input voltage	Input voltage range	4.0		36	V
Input voltage	EN to PGND			$V_{IN}$	V
Input voltage	RT to PGND			5	V
Input voltage	PGOOD to PGND			20	V
Output voltage	SW to PGND			36	V
Output voltage	Output voltage range <sup>(2)</sup>	0.8		28	V
Frequency	Frequency range	200		1000	kHz
Load current	Output DC current range, 3.5A version <sup>(3)</sup>	0		3.5	A
Load current	Output DC current range, 2.5A version <sup>(3)</sup>	0		2.5	A
Temperature	Operating junction temperature $T_J$ range <sup>(4)</sup>	-40		150	$^{\circ}\text{C}$

- (1) Recommended operating conditions indicate conditions for which the device is intended to be functional, but do not specify specific performance limits. For compliant specifications, see Electrical Characteristics table.  
 (2) Under no conditions can the output voltage be allowed to fall below zero volts.  
 (3) Maximum continuous DC current can be derated when operating with high switching frequency or high ambient temperature. See Application section for details.  
 (4) High junction temperatures degrade operating lifetimes. Operating lifetime is de-rated for junction temperatures greater than  $150^{\circ}\text{C}$ .

## 6.4 Thermal Information

THERMAL METRIC <sup>(1)</sup>		LMR514X5-Q1	UNIT
		DRR (WSON)	
		12 PINS	
R <sub>θJA</sub>	Junction-to-ambient thermal resistance	47.4	°C/W
R <sub>θJA(Effecive)</sub>	Junction-to-ambient thermal resistance with TI EVM board	23	°C/W
R <sub>θJC(top)</sub>	Junction-to-case (top) thermal resistance	44.6	°C/W
R <sub>θJB</sub>	Junction-to-board thermal resistance	20.7	°C/W
ψ <sub>JT</sub>	Junction-to-top characterization parameter	0.7	°C/W
ψ <sub>JB</sub>	Junction-to-board characterization parameter	20.7	°C/W
R <sub>θJC(bot)</sub>	Junction-to-case (bottom) thermal resistance	6.3	°C/W

(1) For more information about traditional and new thermal metrics, see the [Semiconductor and IC Package Thermal Metrics](#) application note.

## 6.5 Electrical Characteristics

Limits apply over operating junction temperature ( $T_J$ ) range of  $-40^{\circ}\text{C}$  to  $+150^{\circ}\text{C}$ , unless otherwise stated. Minimum and Maximum limits<sup>(1)</sup> are specified through test, design or statistical correlation. Typical values represent the most likely parametric norm at  $T_J = 25^{\circ}\text{C}$ , and are provided for reference purposes only. Unless otherwise stated, the following conditions apply:  $V_{IN} = 4\text{V}$  to  $36\text{V}$ .

PARAMETER		TEST CONDITIONS	MIN	TYP	MAX	UNIT
<b>SUPPLY VOLTAGE AND CURRENT</b>						
I <sub>Q-nonSW</sub>	Operating quiescent current (non-switching)	V <sub>EN</sub> = 3.3V (PFM variant only)		25		μA
I <sub>SD</sub>	Shutdown quiescent current; measured at VIN pin	V <sub>EN</sub> = 0V, V <sub>IN</sub> = 24V		3	6	μA
V <sub>IN_OPERATE</sub>	V <sub>IN</sub> UVLO threshold	V <sub>IN</sub> rising, needed to start up			3.9	V
		V <sub>IN</sub> falling, once operating	3.4			V
<b>ENABLE</b>						
V <sub>EN-H</sub>	Enable input high level	EN rising, enable switching	1.1	1.25	1.4	V
V <sub>EN-L</sub>	Enable input low level	EN falling, disable switching	0.8	1	1.12	V
I <sub>LKG-EN</sub>	Enable input leakage current	V <sub>EN</sub> = 3.3V		0.1		μA
<b>VOLTAGE REFERENCE (FB PIN)</b>						
V <sub>FB</sub>	Feedback voltage	T <sub>J</sub> = 25°C	0.792	0.8	0.808	V
I <sub>LKG-FB</sub>	Feedback leakage current	FB = 1V			100	nA
<b>CURRENT LIMITS AND HICCUP</b>						
I <sub>SC</sub>	High-side current limit <sup>(3)</sup>	3.5A version	4.5	5.5	6.5	A
I <sub>LS-LIMIT</sub>	Low-side current limit <sup>(3)</sup>	3.5A version		3.7		A
I <sub>SC</sub>	High-side current limit <sup>(3)</sup>	2.5A version	3.3	4.3	5.3	A
I <sub>LS-LIMIT</sub>	Low-side current limit <sup>(3)</sup>	2.5A version		2.7		A
I <sub>L-ZC</sub>	Zero cross detector threshold	PFM variants only		-0.1		A
I <sub>PEAK-MIN</sub>	Minimum inductor peak current <sup>(3)</sup>	3.5A version, PFM variants only		0.7		A
I <sub>PEAK-MIN</sub>	Minimum inductor peak current <sup>(3)</sup>	2.5A version, PFM variants only		0.5		A
I <sub>L-NEG</sub>	Negative current limit <sup>(3)</sup>	3.5A version, FPWM variant only		-1.6		A
I <sub>L-NEG</sub>	Negative current limit <sup>(3)</sup>	2.5A version, FPWM variant only		-1.5		A
V <sub>HICCUP</sub>	Ratio of FB voltage to in-regulation FB voltage			40%		

## 6.5 Electrical Characteristics (continued)

Limits apply over operating junction temperature ( $T_J$ ) range of  $-40^{\circ}\text{C}$  to  $+150^{\circ}\text{C}$ , unless otherwise stated. Minimum and Maximum limits<sup>(1)</sup> are specified through test, design or statistical correlation. Typical values represent the most likely parametric norm at  $T_J = 25^{\circ}\text{C}$ , and are provided for reference purposes only. Unless otherwise stated, the following conditions apply:  $V_{IN} = 4\text{V}$  to  $36\text{V}$ .

PARAMETER		TEST CONDITIONS	MIN	TYP	MAX	UNIT
<b>POWER GOOD</b>						
$V_{PG-HIGH-UP}$	Power-Good upper threshold - rising	% of FB voltage	110%	112%	115%	
$V_{PG-LOW-DN}$	Power-Good lower threshold - falling	% of FB voltage	88%	90%	92%	
$V_{PG-HYS}$	Power-Good hysteresis (rising and falling)	% of FB voltage		2.0%		
$V_{PG-VALID}$	Minimum input voltage for proper Power-Good function				1.5	V
$R_{PG}$	Power-Good ON-resistance	$V_{EN} = 3.3\text{V}$		84		$\Omega$
<b>MOSFETS</b>						
$R_{DS-ON-HS}$	High-side MOSFET ON-resistance			78		m $\Omega$
$R_{DS-ON-LS}$	Low-side MOSFET ON-resistance			45		m $\Omega$
$V_{BOOT-SW-UVLO(R)}$	BOOT-SW UVLO rising threshold	$V_{BOOT-SW}$ rising		2.2		V
<b>SWITCHING CHARACTERISTICS</b>						
$F_{SW (CCM)}$	Switching frequency	$R_T = 34.8\text{k}\Omega$	345	400	455	kHz
$F_{SW (CCM)}$	Switching frequency	$R_T = \text{Open or pull up to voltage } >1.0\text{V}$	395	440	485	kHz
$F_{SW (CCM)}$	Switching frequency	$R_T = 13.3\text{k}\Omega$		1000		kHz
$F_{SW (CCM)}$	Switching frequency	$R_T = \text{Short to GND}$		1000		kHz
$F_{SPREAD}$	Switching frequency dithering	Frequency dithering over center frequency		$\pm 10\%$		
<b>TIMING REQUIREMENT</b>						
$t_{ON-MIN}$	Minimum switch on-time <sup>(2)</sup>	$V_{IN} = 24\text{V}$ , $I_{out} = 1\text{A}$		75		ns
$t_{OFF-MIN}$	Minimum switch off-time			135		ns
$t_{ON-MAX}$	Maximum switch on-time			5		$\mu\text{s}$
$t_{SS}$	Internal soft-start time		3.2	5	7.2	ms
$t_{HICCUP}$	Time between current-limit hiccup burst			96		ms
<b>THERMAL SHUTDOWN</b>						
$T_{SD-Rising}^{(2)}$	Thermal shutdown	Shutdown threshold		160		$^{\circ}\text{C}$
$T_{SD-Falling}^{(2)}$	Thermal shutdown	Recovery threshold		140		$^{\circ}\text{C}$

- (1) MIN and MAX limits are 100% production tested at  $25^{\circ}\text{C}$ . Limits over the operating temperature range verified through correlation using Statistical Quality Control (SQC) methods. Limits are used to calculate Average Outgoing Quality Level (AOQL).
- (2) Not production tested. Specified by correlation by design.
- (3) The current limit values in this table are tested, open loop, in production. They can differ from those found in a closed loop application.

## 6.6 System Characteristics

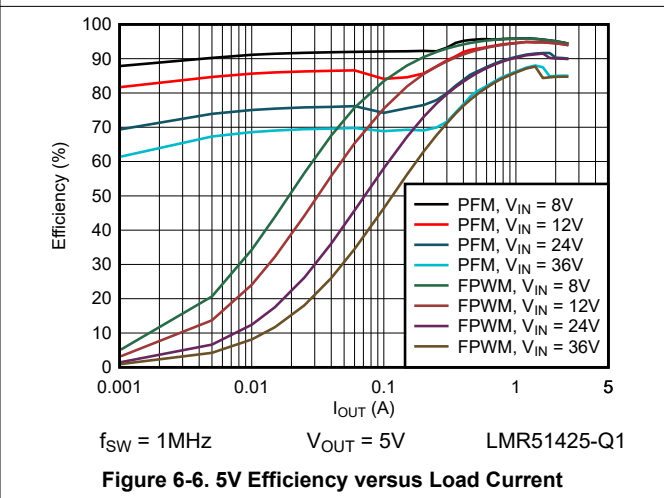
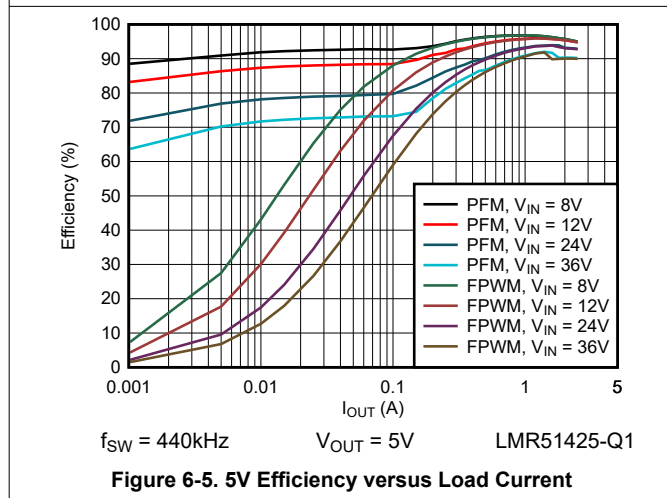
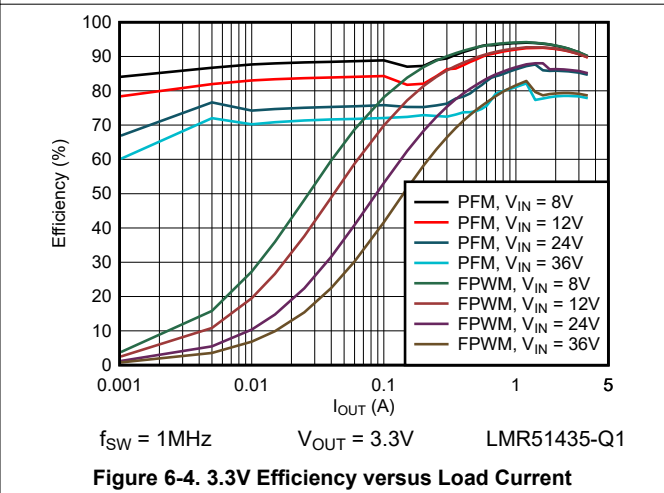
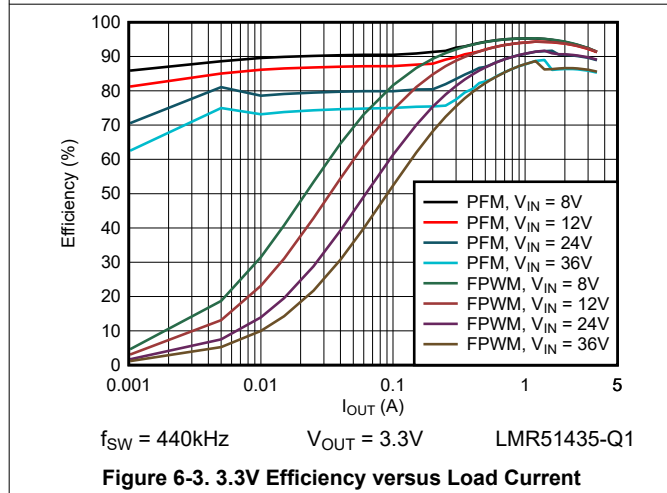
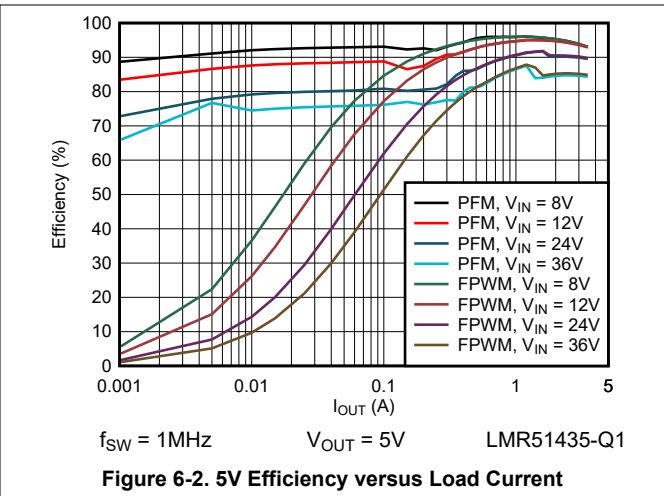
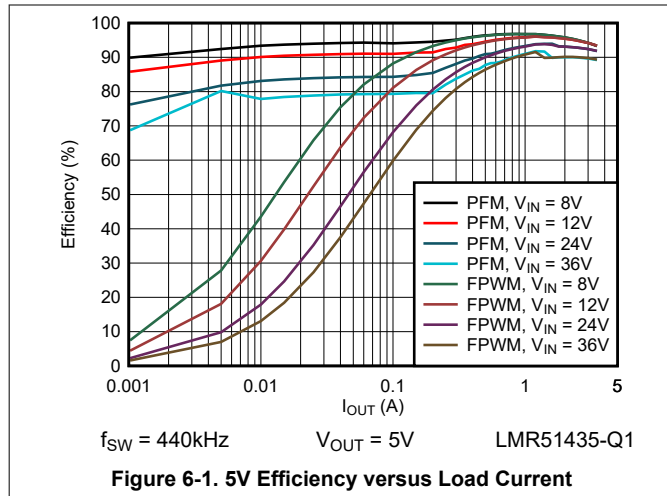
The following specifications apply to a typical application circuit with nominal component values. Specifications in the typical (TYP) column apply to  $T_J = 25^\circ\text{C}$  only. Specifications in the minimum (MIN) and maximum (MAX) columns apply to the case of typical components over the temperature range of  $T_J = -40^\circ\text{C}$  to  $150^\circ\text{C}$ . These specifications are not specified by production testing.

PARAMETER		TEST CONDITIONS	MIN	TYP	MAX	UNIT
$V_{IN}$	Operating input voltage range		4		36	V
$V_{OUT}$	Adjustable output voltage regulation <sup>(1)</sup>	PFM operation		1.5%		
$I_{SUPPLY}$	Input supply current when in regulation	$V_{IN} = 24\text{V}$ , $V_{OUT} = 3.3\text{V}$ , $I_{OUT} = 0\text{A}$ , $R_{FBT} = 1\text{M}\Omega$ , PFM variant		35		$\mu\text{A}$
$D_{MAX}$	Maximum switch duty cycle <sup>(2)</sup>			97%		
$V_{HC}$	FB pin voltage required to trip short-circuit hiccup mode			0.32		V

- (1) Deviation in  $V_{OUT}$  from nominal output voltage value at  $V_{IN} = 24\text{V}$ ,  $I_{OUT} = 0\text{A}$  to full load  
(2) In dropout the switching frequency drops to increase the effective duty cycle. The lowest frequency is clamped at approximately:  $F_{MIN} = 1 / (t_{ON-MAX} + t_{OFF-MIN})$ .  $D_{MAX} = t_{ON-MAX} / (t_{ON-MAX} + t_{OFF-MIN})$ .

## 6.7 Typical Characteristics

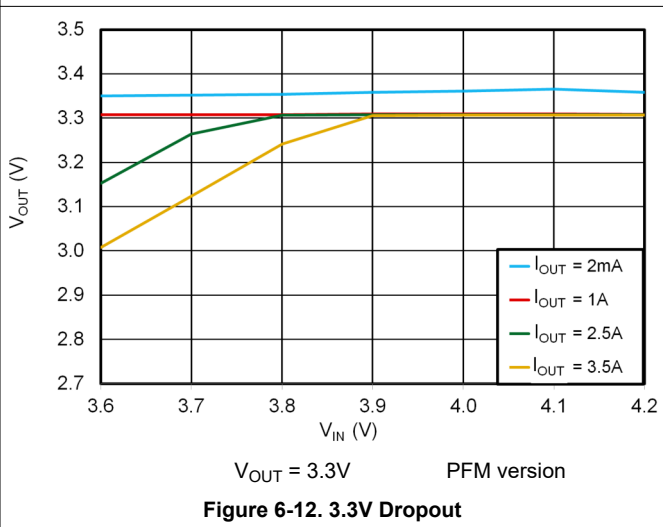
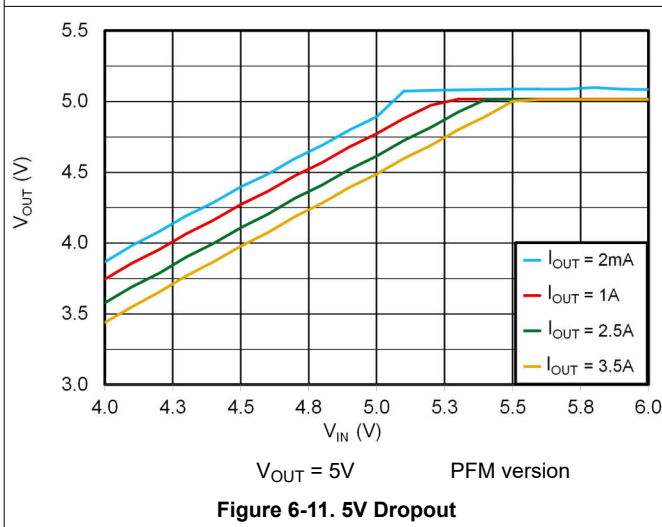
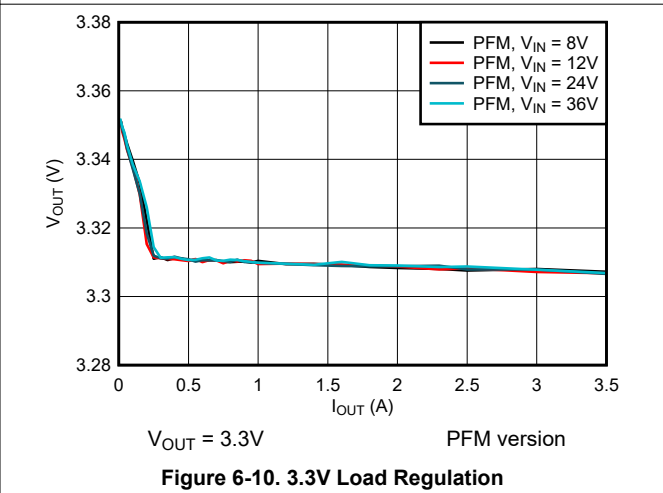
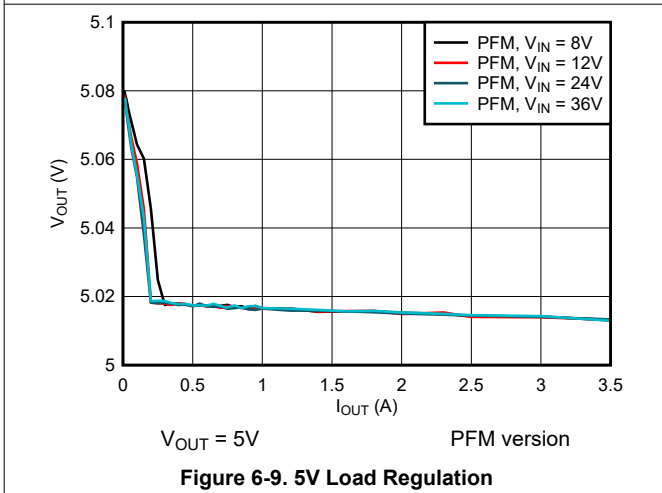
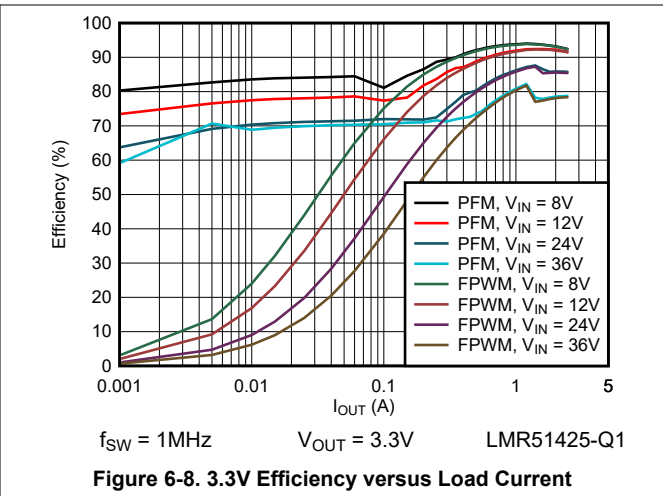
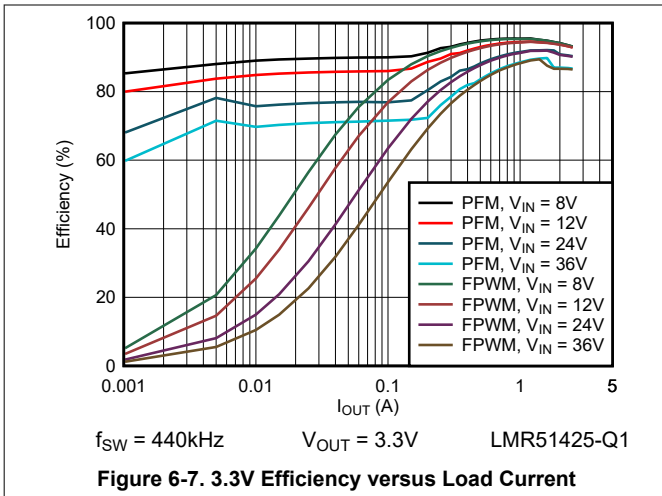
$V_{IN} = 12V$ ,  $f_{SW} = 440kHz$ ,  $T_A = 25^{\circ}C$ , unless otherwise specified.





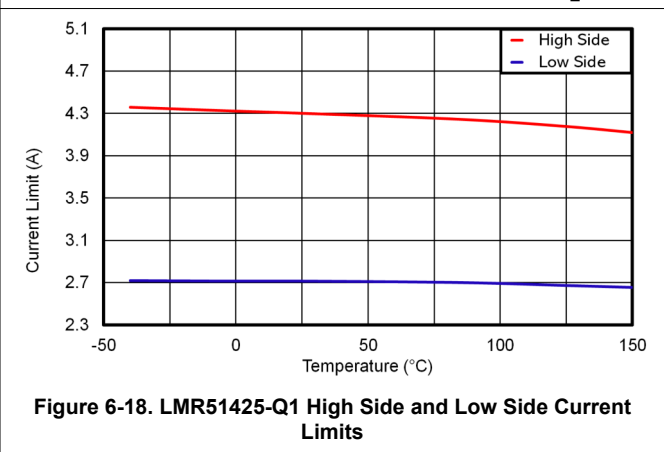
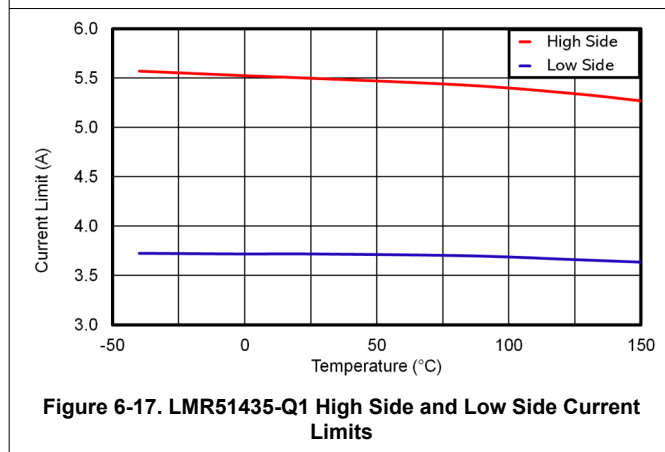
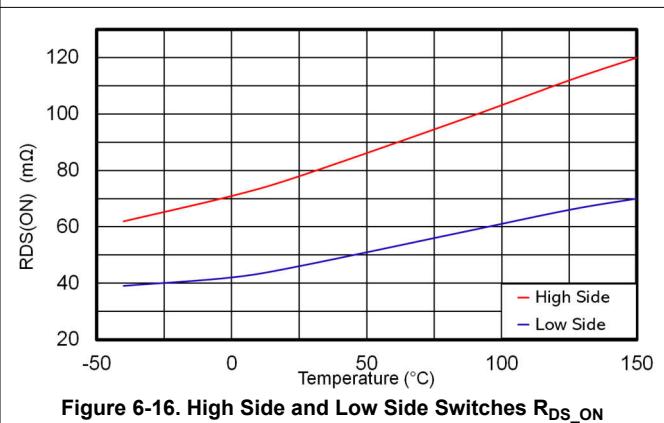
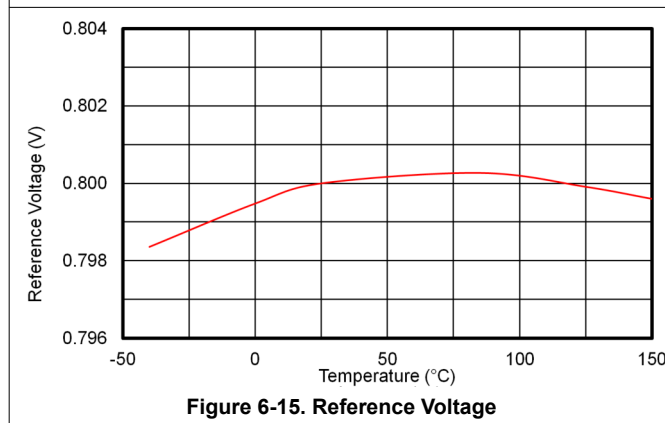
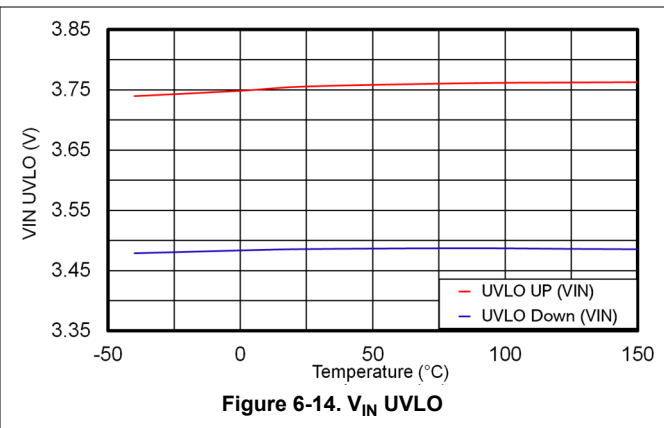
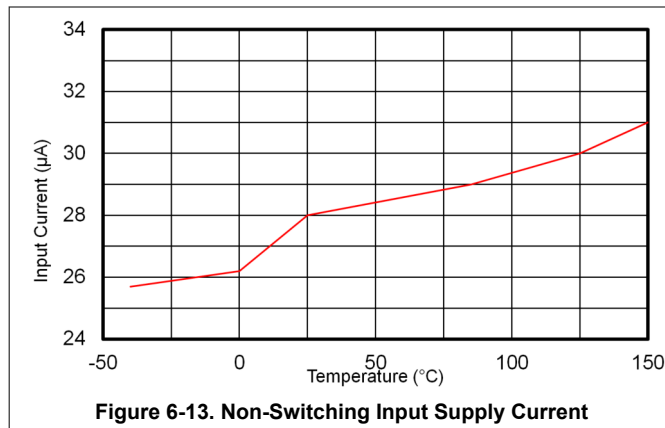
### 6.7 Typical Characteristics (continued)

$V_{IN} = 12V$ ,  $f_{SW} = 440kHz$ ,  $T_A = 25^\circ C$ , unless otherwise specified.



## 6.7 Typical Characteristics (continued)

$V_{IN} = 12V$ ,  $f_{SW} = 440kHz$ ,  $T_A = 25^{\circ}C$ , unless otherwise specified.



## 7 Detailed Description

### 7.1 Overview

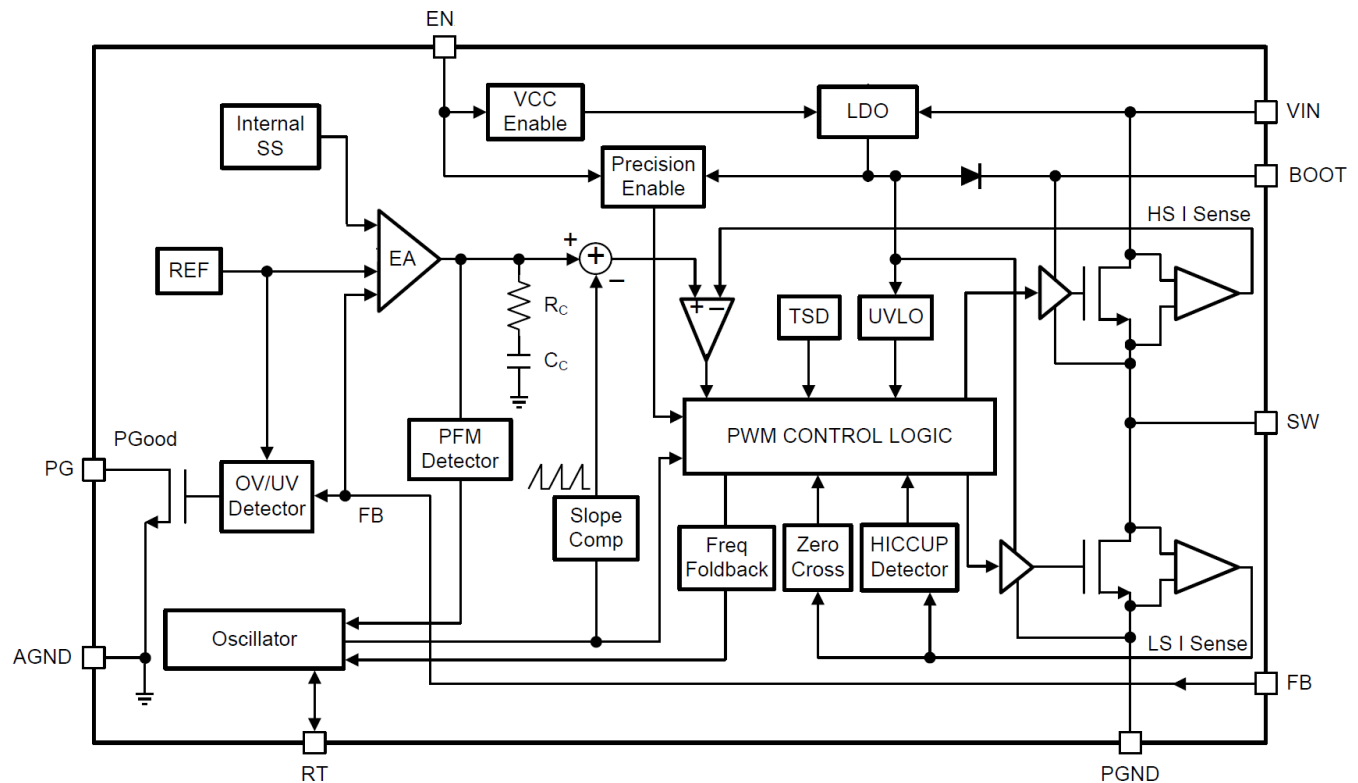
The LMR514x5-Q1 converter is an easy-to-use, synchronous, step-down DC/DC converter operating from a 4V to 36V supply voltage. The device is capable of delivering up to 2.5A or 3.5A DC load current in a very small design size. The family has multiple versions applicable to various applications. See [Device Comparison Table](#) for detailed information.

The LMR514x5-Q1 employs fixed-frequency peak-current mode control. The PFM version enters PFM mode at light load to achieve high efficiency. A FPWM version is provided to achieve low output voltage ripple, tight output voltage regulation, and constant switching frequency at light load. The device is internally compensated, which reduces design time and requires few external components.

Additional features, such as precision enable and internal soft start, provide a flexible and easy-to-use solution for a wide range of applications. Protection features include thermal shutdown,  $V_{IN}$  undervoltage lockout, cycle-by-cycle current limit, and hiccup mode short-circuit protection.

This family of devices requires very few external components and has a pinout designed for simple, optimum PCB layout.

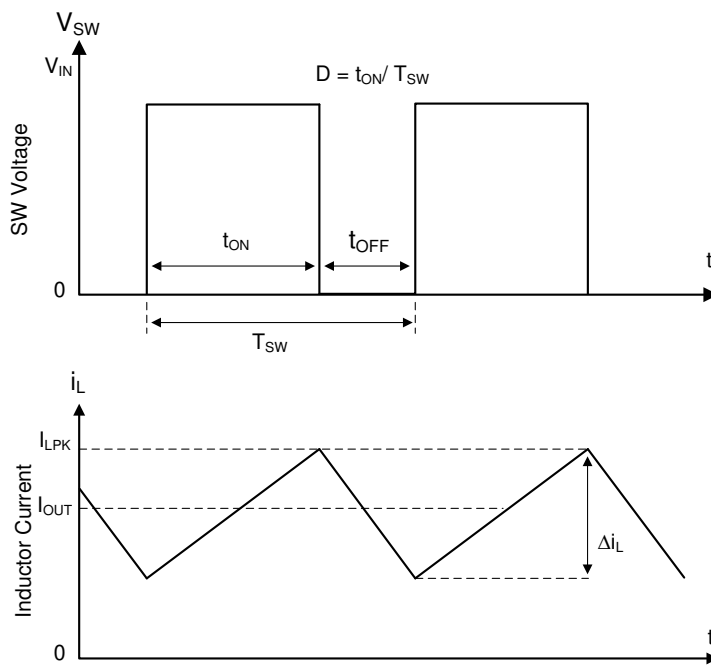
### 7.2 Functional Block Diagram



## 7.3 Feature Description

### 7.3.1 Fixed Frequency Peak Current Mode Control

The following operating description of the LMR514x5-Q1 refers to [Functional Block Diagram](#) and to the waveforms in [Figure 7-1](#). The LMR514x5-Q1 is a step-down synchronous buck converter with integrated high-side (HS) and low-side (LS) switches (synchronous rectifier). The LMR514x5-Q1 supplies a regulated output voltage by turning on the high-side and low-side NMOS switches with controlled duty cycle. During high-side switch ON time, the SW pin voltage swings up to approximately  $V_{IN}$ , and the inductor current,  $i_L$ , increases with linear slope  $(V_{IN} - V_{OUT}) / L$ . When the high-side switch is turned off by the control logic, the low-side switch is turned on after an anti-shoot-through dead time. Inductor current discharges through the low-side switch with a slope of  $-V_{OUT} / L$ . The control parameter of a buck converter is defined as Duty Cycle  $D = t_{ON} / T_{SW}$ , where  $t_{ON}$  is the high-side switch ON time and  $T_{SW}$  is the switching period. The converter control loop maintains a constant output voltage by adjusting the duty cycle  $D$ . In an ideal buck converter, where losses are ignored,  $D$  is proportional to the output voltage and inversely proportional to the input voltage:  $D = V_{OUT} / V_{IN}$ .



**Figure 7-1. SW Node and Inductor Current Waveforms in Continuous Conduction Mode (CCM)**

The LMR514x5-Q1 employs fixed-frequency peak-current mode control. A voltage feedback loop is used to get accurate DC voltage regulation by adjusting the peak-current command based on voltage offset. The peak inductor current is sensed from the high-side switch and compared to the peak current threshold to control the ON time of the high-side switch. The voltage feedback loop is internally-compensated, which allows for fewer external components, making designing easy, and providing stable operation when using a variety of output capacitors. The converter operates with fixed switching frequency at normal load conditions. During light-load condition, the LMR514x5-Q1 operates in PFM mode to maintain high efficiency (PFM version) or in FPWM mode for low output voltage ripple, tight output voltage regulation, and constant switching frequency (FPWM version).

### 7.3.2 Adjustable Output Voltage

A precision 0.8V reference voltage ( $V_{REF}$ ) is used to maintain a tightly regulated output voltage over the entire operating temperature range. The output voltage is set by a resistor divider from  $V_{OUT}$  to the FB pin. TI recommends to use 1% tolerance resistors with a low temperature coefficient for the FB divider. Select the bottom-side resistor  $R_{FBB}$  for the desired divider current and use Equation 1 to calculate top-side resistor  $R_{FBT}$ . The recommended range for  $R_{FBT}$  is 10k $\Omega$  to 100k $\Omega$ . A lower  $R_{FBT}$  value can be used if pre-loading is desired to reduce  $V_{OUT}$  offset in PFM operation. Lower  $R_{FBT}$  reduces efficiency at very light load. Less static current goes through a larger  $R_{FBT}$  and can be more desirable when light-load efficiency is critical. However, TI does not recommend  $R_{FBT}$  larger than 1M $\Omega$  because  $R_{FBT}$  larger than 1M $\Omega$  makes the feedback path more susceptible to noise. Larger  $R_{FBT}$  values require more carefully designed feedback path trace from the feedback resistors to the feedback pin of the device. The tolerance and temperature variation of the resistor divider network affect the output voltage regulation.

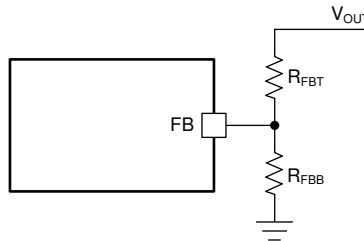


Figure 7-2. Output Voltage Setting

$$R_{FBT} = \frac{(V_{OUT} - V_{REF})}{V_{REF}} \times R_{FBB} \quad (1)$$

### 7.3.3 Enable

The voltage on the EN pin controls the ON and OFF operation of the LMR514x5-Q1. A voltage of less than 0.8V shuts down the device, while a voltage of greater than 1.4V is required to start the converter. The EN pin is an input and cannot be left open or floating. The simplest way to enable the operation of the LMR514x5-Q1 when  $V_{IN}$  is within the operating range.

Many applications benefit from the employment of an enable divider  $R_{ENT}$  and  $R_{ENB}$  (Figure 7-3) to establish a precision system UVLO level for the converter. System UVLO can be used for supplies operating from utility power as well as battery power. System UVLO can be used for sequencing, making sure of reliable operation or supplying protection, such as a battery discharge level. An external logic signal can also be used to drive EN input for system sequencing and protection. Note, the EN pin voltage must not to be greater than  $V_{IN} + 0.3V$ . TI does not recommend to apply EN voltage when  $V_{IN}$  is 0V.

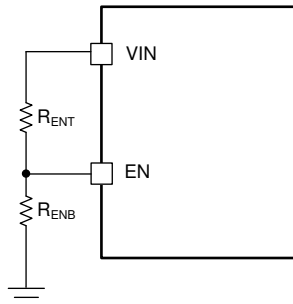


Figure 7-3. System UVLO by Enable Divider

### 7.3.4 Switching Frequency

The switching frequency of the LMR514x5-Q1 can be programmed by the resistor  $R_T$  from the  $R_T$  pin and GND pin. The  $R_T$  pin cannot be left floating or shorted to ground. To determine the timing resistance for a given switching frequency, use Equation 2 or the curve in Figure 7-4. Table 7-1 gives typical  $R_T$  values for a given  $f_{SW}$ .

$$R_T(\text{k}\Omega) = 18576 \times f_{SW}(\text{kHz})^{-1.048} \quad (2)$$

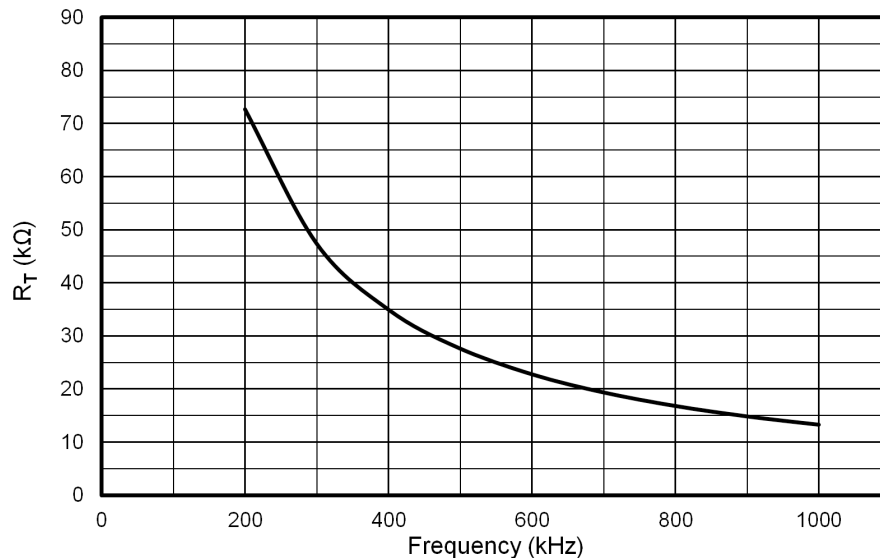


Figure 7-4.  $R_T$  Versus Frequency Curve

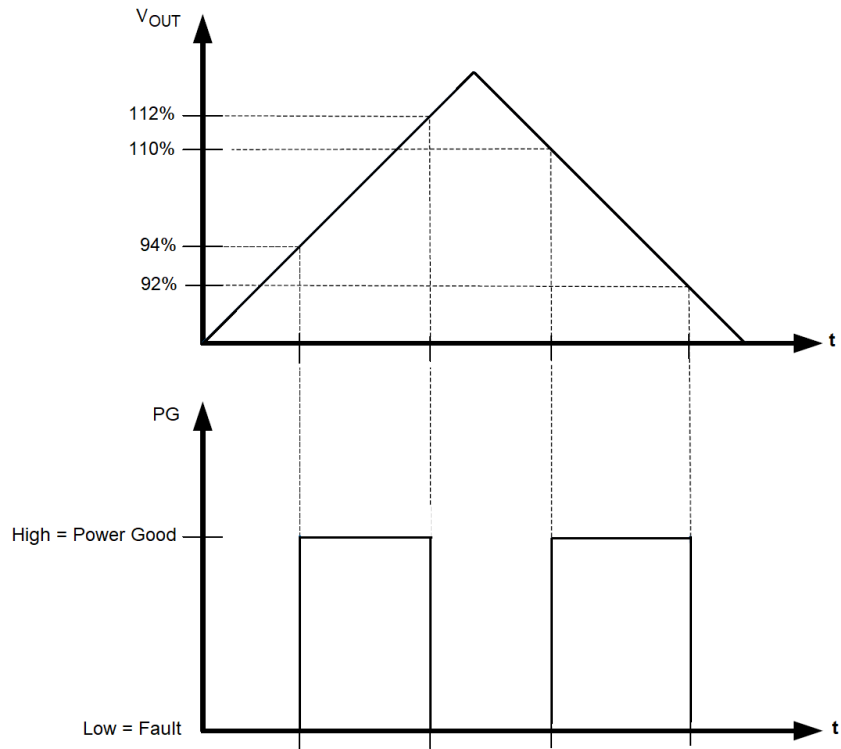
Table 7-1. Typical Frequency Setting  $R_T$  Resistance

$f_{SW}$ (kHz)	$R_T$ (kΩ)
200	71.5
400	34.8
440	Open or pull up to voltage > 1.0V
500	27.4
750	18.0
1000	13.3
1000	Short to GND

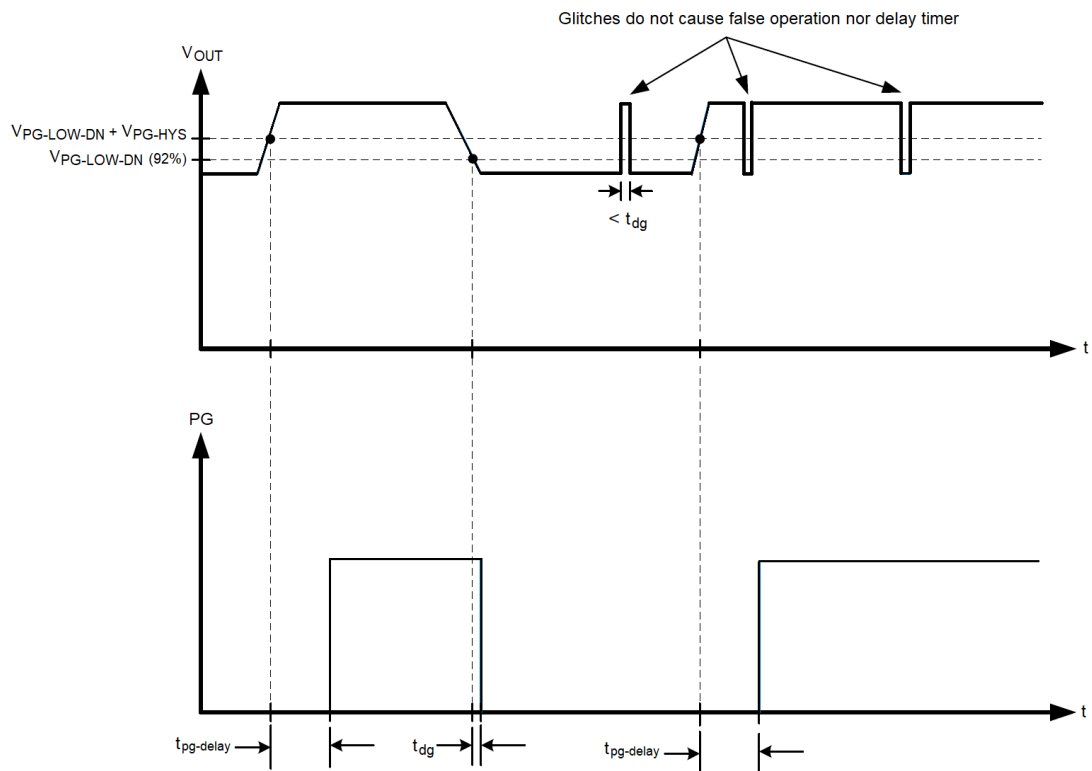
### 7.3.5 Power-Good Flag Output

The power-good flag function (PG output pin) of the LMR514x5-Q1 can be used to reset a system microprocessor whenever the output voltage is out of regulation. This open-drain output goes low under fault conditions, such as current limit and thermal shutdown, as well as during normal start-up. A glitch filter prevents false flag operation for short excursions of the output voltage, such as during line and load transients. Output voltage excursions lasting less than  $t_{dg}$  35μs (typical) do not trip the power-good flag. After the FB voltage has returned to the regulation value and after a delay of  $t_{pg-delay}$  3.1ms (typical), the power-good flag goes high.

The power-good output consists of an open-drain NMOS, requiring an external pullup resistor to a suitable logic supply. It can be pulled up to power supply below 20V through a 10kΩ to 100kΩ resistor, as desired. If this function is not needed, the PG pin must be left floating. When EN is pulled low, the flag output is also forced low. With EN low, power good remains valid as long as the input voltage is greater than or equal to 1.5V (typical). Limit the current into the power-good flag pin to less than 5mA D.C.



**Figure 7-5. Static Power-Good Operation**



**Figure 7-6. Power-Good Timing Behavior**

### 7.3.6 Minimum ON-Time, Minimum OFF-Time, and Frequency Foldback

Minimum ON-time ( $t_{ON\_MIN}$ ) is the shortest duration of time that the high-side switch can be turned on.  $t_{ON\_MIN}$  is typically 75ns for the LMR514x5-Q1. Minimum OFF-time ( $t_{OFF\_MIN}$ ) is the shortest duration of time that the high-side switch can be off.  $t_{OFF\_MIN}$  is typically 135ns. In CCM operation,  $t_{ON\_MIN}$  and  $t_{OFF\_MIN}$  limit the voltage conversion range without switching frequency foldback.

The minimum duty cycle without frequency foldback allowed is:

$$D_{MIN} = t_{ON\_MIN} \times f_{SW} \quad (3)$$

The maximum duty cycle without frequency foldback allowed is:

$$D_{MAX} = 1 - t_{OFF\_MIN} \times f_{SW} \quad (4)$$

Given a required output voltage, the maximum  $V_{IN}$  without frequency foldback can be found by:

$$V_{IN\_MAX} = \frac{V_{OUT}}{f_{SW} \times t_{ON\_MIN}} \quad (5)$$

The minimum  $V_{IN}$  without frequency foldback can be calculated by:

$$V_{IN\_MIN} = \frac{V_{OUT}}{1 - f_{SW} \times t_{OFF\_MIN}} \quad (6)$$

In the LMR514x5-Q1, a frequency foldback scheme is employed after the  $t_{ON\_MIN}$  or  $t_{OFF\_MIN}$  is triggered, which can extend the maximum duty cycle or lower the minimum duty cycle.

The on-time decreases while  $V_{IN}$  voltage increases. After the on-time decreases to  $t_{ON\_MIN}$ , the switching frequency starts to decrease while  $V_{IN}$  continues to go up, which lowers the duty cycle further to keep  $V_{OUT}$  in regulation according to [Equation 5](#).

The frequency foldback scheme also works after larger duty cycle is needed under low  $V_{IN}$  condition. The frequency decreases after the device hits the  $t_{OFF\_MIN}$ , which extends the maximum duty cycle according to [Equation 6](#). In such condition, the frequency can be as low as approximately 200kHz. Wide range of frequency foldback allows for the LMR514x5-Q1 output voltage to stay in regulation with a much lower supply voltage  $V_{IN}$ , which leads to a lower effective dropout.

With frequency foldback while maintaining a regulated output voltage,  $V_{IN\_MAX}$  is raised, and  $V_{IN\_MIN}$  is lowered by decreased  $f_{SW}$ .

### 7.3.7 Bootstrap Voltage

The LMR514x5-Q1 provides an integrated bootstrap voltage converter. A small capacitor between the CB and SW pins provides the gate drive voltage for the high-side MOSFET. The bootstrap capacitor is refreshed when the high-side MOSFET is off and the low-side switch is on. The recommended value of the bootstrap capacitor is 0.1 $\mu$ F. TI recommends a ceramic capacitor with an X7R or X5R grade dielectric with a voltage rating of 16V or higher for stable performance over temperature and voltage.

### 7.3.8 Overcurrent and Short-Circuit Protection

The LMR514x5-Q1 incorporates both peak and valley inductor current limit to provide protection to the device from overloads and short circuits and limit the maximum output current. Valley current limit prevents inductor current runaway during short circuits on the output, while both peak and valley limits work together to limit the maximum output current of the converter. Cycle-by-cycle current limit is used for overloads, while hiccup mode is used for sustained short circuits.

High-side MOSFET overcurrent protection is implemented by the nature of the peak current mode control. The high-side switch current is sensed when the high-side is turned on after a set blanking time. The high-side switch current is compared to the output of the Error Amplifier (EA) minus slope compensation every switching cycle.



See [Functional Block Diagram](#) for more details. The peak current of high-side switch is limited by a clamped maximum peak current threshold  $I_{sc}$  which is constant.

The current going through low-side MOSFET is also sensed and monitored. When the low-side switch turns on, the inductor current begins to ramp down. The low-side switch is not turned OFF at the end of a switching cycle if the current is above the low-side current limit  $I_{LS\_LIMIT}$ . The low-side switch is kept ON so that inductor current keeps ramping down, until the inductor current ramps below the  $I_{LS\_LIMIT}$ . Then the low-side switch is turned OFF and the high-side switch is turned on after a dead time. After  $I_{LS\_LIMIT}$  is achieved, peak and valley current limit controls the maximum current deliver and can be calculated using the following equation.

$$I_{OUT\_MAX} = \frac{I_{LS\_LIMIT} + I_{SC}}{2} \quad (7)$$

If the feedback voltage is lower than 40% of the  $V_{REF}$ , the current of the low-side switch triggers  $I_{LS\_LIMIT}$  for 128 consecutive cycles and hiccup current protection mode is activated. In hiccup mode, the converter shuts down and keeps off for a period of hiccup,  $T_{HICCUP}$  (96ms typical) before the LMR514x5-Q1 tries to start again. If overcurrent or short-circuit fault condition still exist, hiccup repeats until the fault condition is removed. Hiccup mode reduces power dissipation under severe overcurrent conditions, prevents over-heating and potential damage to the device.

For FPWM version, the inductor current is allowed to go negative. When this current exceeds the low-side negative current limit  $I_{LS\_NEG}$ , the low-side switch is turned off and high-side switch is turned on immediately. This is used to protect the low-side switch from excessive negative current.

### 7.3.9 Soft Start

The integrated soft-start circuit prevents input inrush current impacting the LMR514x5-Q1 and the input power supply. Soft start is achieved by slowly ramping up the internal reference voltage when the device is first enabled or powered up. The typical soft-start time is 5ms.

### 7.3.10 Thermal Shutdown

The LMR514x5-Q1 provides an internal thermal shutdown to protect the device when the junction temperature exceeds 160°C. Both high-side and low-side FETs stop switching in thermal shutdown. After the die temperature falls below 140°C, the device reinitiates the power-up sequence controlled by the internal soft-start circuitry.

## 7.4 Device Functional Modes

### 7.4.1 Shutdown Mode

The EN pin provides electrical ON and OFF control for the LMR514x5-Q1. When  $V_{EN}$  is below 0.8V, the device is in shutdown mode. The LMR514x5-Q1 also employs  $V_{IN}$  undervoltage lockout protection (UVLO). If  $V_{IN}$  voltage is below the UVLO threshold 3.4V, the converter is turned off.

### 7.4.2 Active Mode

The LMR514x5-Q1 is in active mode when both  $V_{EN}$  and  $V_{IN}$  are above the respective operating threshold. The simplest way to enable the LMR514x5-Q1 is to connect the EN pin to VIN pin. This connection allows self-start-up when the input voltage is in the operating range of 4V to 36V. See [Enable](#) for details on setting these operating levels.

In active mode, depending on the load current, the LMR514x5-Q1 is in one of four modes:

1. Continuous conduction mode (CCM) with fixed switching frequency when load current is greater than half of the peak-to-peak inductor current ripple (for both PFM and FPWM versions)
2. Discontinuous conduction mode (DCM) with fixed switching frequency when load current is less than half of the peak-to-peak inductor current ripple(only for PFM version)
3. Pulse frequency modulation mode (PFM) when switching frequency is decreased at very light load (only for PFM version)
4. Forced pulse width modulation mode (FPWM) with fixed switching frequency even at light load (only for FPWM version)

### 7.4.3 CCM Mode

Continuous Conduction Mode (CCM) operation is employed in the LMR514x5-Q1 when the load current is greater than half of the peak-to-peak inductor current. In CCM operation, the frequency of operation is fixed, output voltage ripple is at a minimum in this mode, and the maximum output current of 2.5A or 3.5A can be supplied by the LMR51425-Q1 or LMR51435-Q1 respectively.

### 7.4.4 Light-Load Operation (PFM Version)

For PFM version, when the load current is lower than half of the peak-to-peak inductor current in CCM, the LMR514x5-Q1 operates in Discontinuous Conduction Mode (DCM), also known as Diode Emulation Mode (DEM). In DCM operation, the low-side switch is turned off when the inductor current drops to  $I_{LS\_ZC}$  (100mA typical) to improve efficiency. Both switching losses and conduction losses are reduced in DCM, compared to forced PWM operation at light load.

During light load operation, Pulse Frequency Modulation (PFM) mode is activated to maintain high efficiency operation. When either the minimum high-side switch ON time  $t_{ON\_MIN}$  or the minimum peak inductor current  $I_{PEAK\_MIN}$  (0.7A for LMR51435-Q1 and 0.5A for LMR51425-Q1) is reached, the switching frequency decreases to maintain regulation. In PFM mode, switching frequency is decreased by the control loop to maintain output voltage regulation when load current reduces. Switching loss is further reduced in PFM operation due to a significant drop in effective switching frequency.

### 7.4.5 Light-Load Operation (FPWM Version)

For FPWM version, LMR514x5-Q1 is locked in PWM mode at full load range. This operation is maintained, even in no-load condition, by allowing the inductor current to reverse the normal direction. This mode trades off reduced light load efficiency for low output voltage ripple, tight output voltage regulation, and constant switching frequency.

## 8 Application and Implementation

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### Note

Information in the following applications sections is not part of the TI component specification, and TI does not warrant its accuracy or completeness. TI's customers are responsible for determining suitability of components for their purposes, as well as validating and testing their design implementation to confirm system functionality.

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### 8.1 Application Information

The LMR514x5-Q1 is a step-down DC-to-DC converter. The device is typically used to convert a higher input voltage to a lower output DC voltage with a maximum output current of 2.5A or 3.5A. The following design procedure can be used to select components for the LMR514x5-Q1. Alternately, the WEBENCH software can be used to generate complete designs. When generating a design, the WEBENCH software uses iterative design procedure and accesses comprehensive databases of components. Go to [ti.com](https://www.ti.com) for more details.

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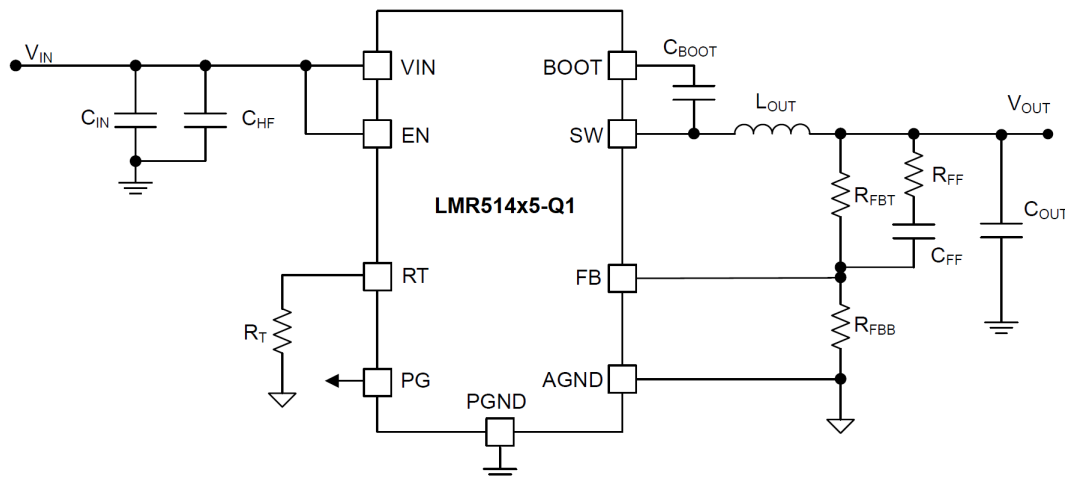
### Note

All of the capacitance values given in the following application information refer to *effective* values unless otherwise stated. The *effective* value is defined as the actual capacitance under DC bias and temperature, not the rated or nameplate values. Use high-quality, low-ESR, ceramic capacitors with an X7R or better dielectric throughout. All high value ceramic capacitors have a large voltage coefficient in addition to normal tolerances and temperature effects. Under DC bias the capacitance drops considerably. Large case sizes and higher voltage ratings are better in this regard. To help mitigate these effects, multiple capacitors can be used in parallel to bring the minimum *effective* capacitance up to the required value. This can also ease the RMS current requirements on a single capacitor. A careful study of bias and temperature variation of any capacitor bank must be made to make sure that the minimum value of *effective* capacitance is provided.

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## 8.2 Typical Application

The LMR514x5-Q1 only requires a few external components to convert from a wide voltage range supply to a fixed output voltage. Figure 8-1 shows a basic schematic.



**Figure 8-1. Application Circuit**

The external components have to fulfill the needs of the application and the stability criteria of the control loop of the device. Use the following tables to simplify the output filter component selection.

**Table 8-1. L and C<sub>OUT</sub> Typical Values for LMR51425-Q1**

f <sub>sw</sub> (kHz)	V <sub>OUT</sub> (V)	L (μH)	C <sub>OUT</sub> (μF) <sup>(1)</sup>	R <sub>FBT</sub> (kΩ)	R <sub>FBB</sub> (kΩ)	C <sub>FF</sub> (pF)	R <sub>FF</sub> (kΩ)
440	3.3	6.8	56	100	31.6	27	1
	5	8.2	33	100	19.1	27	1
1000	3.3	3.3	27	100	31.6	18	1
	5	4.7	18	100	19.1	18	1

(1) A ceramic capacitor is used in this table. All the C<sub>OUT</sub> values are after derating.

**Table 8-2. L and C<sub>OUT</sub> Typical Values for LMR51435-Q1**

f <sub>sw</sub> (kHz)	V <sub>OUT</sub> (V)	L (μH)	C <sub>OUT</sub> (μF) <sup>(1)</sup>	R <sub>FBT</sub> (kΩ)	R <sub>FBB</sub> (kΩ)	C <sub>FF</sub> (pF)	R <sub>FF</sub> (kΩ)
440	3.3	4.7	75	100	31.6	27	1
	5	6.8	47	100	19.1	27	1
1000	3.3	2.7	39	100	31.6	18	1
	5	3.3	27	100	19.1	18	1

(1) A ceramic capacitor is used in this table. All the C<sub>OUT</sub> values are after derating.

### 8.2.1 Design Requirements

The detailed design procedure is described based on a design example. For this design example, use the parameters listed in the following table as the input parameters.

**Table 8-3. Design Example Parameters**

PARAMETER	VALUE
Input voltage, $V_{IN}$	12V typical, range from 6V to 36V
Output voltage, $V_{OUT}$	5V $\pm$ 3%
Maximum output current, $I_{OUT\_MAX}$	3.5A
Output overshoot, undershoot (0.87A to 2.63A)	5%
Output voltage ripple	0.5%
Operating frequency	440kHz

### 8.2.2 Detailed Design Procedure

#### 8.2.2.1 Custom Design With WEBENCH® Tools

[Click here](#) to create a custom design using the LMR514x5-Q1 device with the WEBENCH Power Designer.

1. Start by entering the input voltage ( $V_{IN}$ ), output voltage ( $V_{OUT}$ ), and output current ( $I_{OUT}$ ) requirements.
2. Optimize the design for key parameters such as efficiency, footprint, and cost using the optimizer dial.
3. Compare the generated design with other possible solutions from Texas Instruments.

The WEBENCH Power Designer provides a customized schematic along with a list of materials with real-time pricing and component availability.

In most cases, these actions are available:

- Run electrical simulations to see important waveforms and circuit performance
- Run thermal simulations to understand board thermal performance
- Export customized schematic and layout into popular CAD formats
- Print PDF reports for the design, and share the design with colleagues

Get more information about WEBENCH tools at [www.ti.com/WEBENCH](http://www.ti.com/WEBENCH).

#### 8.2.2.2 Output Voltage Set-Point

The output voltage of the LMR514x5-Q1 device is externally adjustable using a resistor divider network. The divider network is comprised of top feedback resistor  $R_{FBT}$  and bottom feedback resistor  $R_{FBB}$ . Use the following equation to determine the output voltage of the converter:

$$R_{FBT} = \frac{(V_{OUT} - V_{REF})}{V_{REF}} \times R_{FBB} \quad (8)$$

Choose the value of  $R_{FBB}$  to be 19.1k $\Omega$ . With the desired output voltage set to 5V and the  $V_{REF} = 0.8V$ , the  $R_{FBT}$  value can then be calculated using [Equation 8](#). The formula yields to a value 100.28k $\Omega$ , a standard value of 100k $\Omega$  is selected.

#### 8.2.2.3 Switching Frequency

The higher switching frequency allows for lower value inductors and smaller output capacitors, which results in smaller design size and lower component cost. However, higher switching frequency brings more switching loss, making the design less efficient and produce more heat. The switching frequency is also limited by the minimum on-time of the integrated power switch, the input voltage, the output voltage, and the frequency shift limitation as mentioned in [Minimum ON-Time, Minimum OFF-Time, and Frequency Foldback](#).

For this example, a switching frequency of 440kHz is selected. RT open defaults to 440kHz.

### 8.2.2.4 Inductor Selection

The most critical parameters for the inductor are the inductance, saturation current, and the RMS current. The inductance is based on the desired peak-to-peak ripple current  $\Delta i_L$ . Because the ripple current increases with the input voltage, the maximum input voltage is always used to calculate the minimum inductance  $L_{MIN}$ . Use Equation 10 to calculate the minimum value of the output inductor.  $K_{IND}$  is a coefficient that represents the amount of inductor ripple current relative to the maximum output current of the device. A reasonable value of  $K_{IND}$  must be 20% to 60% of maximum  $I_{OUT}$  supported by converter. During an instantaneous overcurrent operation event, the RMS and peak inductor current can be high. The inductor saturation current must be higher than peak current limit level.

$$\Delta i_L = \frac{V_{OUT} \times (V_{IN\_MAX} - V_{OUT})}{V_{IN\_MAX} \times L \times f_{SW}} \quad (9)$$

$$L_{MIN} = \frac{V_{IN\_MAX} - V_{OUT}}{I_{OUT} \times K_{IND}} \times \frac{V_{OUT}}{V_{IN\_MAX} \times f_{SW}} \quad (10)$$

In general, choosing lower inductance in switching power supplies is preferable because lower inductance usually corresponds to faster transient response, smaller DCR, and reduced size for more compact designs. Too low of an inductance can generate too large of an inductor current ripple such that overcurrent protection at the full load can be falsely triggered. Too low of an inductance also generates more inductor core loss because the current ripple is larger. Larger inductor current ripple also implies larger output voltage ripple with the same output capacitors. With peak current mode control, TI recommends to have adequate amount of inductor ripple current. A larger inductor ripple current improves the comparator signal-to-noise ratio.

For this design example, choose  $K_{IND} = 0.45$ . The minimum inductor value is calculated to be 6.21 $\mu$ H. Choose the nearest standard 6.8 $\mu$ H power inductor with a capability of 4.2A RMS current and 7A saturation current.

### 8.2.2.5 Output Capacitor Selection

The device is designed to be used with a wide variety of LC filters. Minimize the output capacitance to keep cost and size down. The output capacitor or capacitors,  $C_{OUT}$ , must be chosen with care because capacitor or capacitors directly affects the steady state output voltage ripple, loop stability, and output voltage overshoot and undershoot during load current transient. The output voltage ripple is essentially composed of two parts. One part is caused by the inductor ripple current flowing through the Equivalent Series Resistance (ESR) of the output capacitors:

$$\Delta V_{OUT\_ESR} = \Delta i_L \times ESR = K_{IND} \times I_{OUT} \times ESR \quad (11)$$

The other part is caused by the inductor current ripple charging and discharging the output capacitors:

$$\Delta V_{OUT\_C} = \frac{\Delta i_L}{8 \times f_{SW} \times C_{OUT}} = \frac{K_{IND} \times I_{OUT}}{8 \times f_{SW} \times C_{OUT}} \quad (12)$$

The two components of the voltage ripple are not in-phase, therefore, the actual peak-to-peak ripple is less than the sum of the two peaks.

Output capacitance is usually limited by transient performance specifications if the system requires tight voltage regulation with presence of large current steps and fast slew rates. When a large load step occurs, output capacitors provide the required charge before the inductor current can slew to an appropriate level. The control loop of the converter usually requires eight or more clock cycles to regulate the inductor current equal to the new load level during this time. The output capacitance must be large enough to supply the current difference for 6 clock cycles to maintain the output voltage within the specified range. The following equation shows the minimum output capacitance needed for a specified  $V_{OUT}$  overshoot and undershoot.

$$C_{OUT} > \frac{1}{2} \times \frac{6 \times (I_{OH} - I_{OL})}{f_{SW} \times \Delta V_{OUT\_SHOOT}} \quad (13)$$

where

- $K_{IND}$  = Ripple ratio of the inductor current ( $\Delta i_L / I_{OUT}$ )
- $I_{OL}$  = Low level output current during load transient
- $I_{OH}$  = High level output current during load transient
- $V_{OUT\_SHOOT}$  = Target output voltage overshoot or undershoot

For this design example, the target output ripple is 25mV. Assuming  $\Delta V_{OUT\_ESR} = \Delta V_{OUT\_C} = 25\text{mV}$ , choose  $K_{IND} = 0.45$ . Equation 11 yields ESR no larger than 15.9m $\Omega$  and Equation 12 yields  $C_{OUT}$  no smaller than 17.9 $\mu\text{F}$ . For the target overshoot and undershoot limitation of this design,  $\Delta V_{OUT\_SHOOT}$  is 250mV. The  $C_{OUT}$  can be calculated to be no less than 47.7 $\mu\text{F}$  by Equation 13. In summary, the most stringent criteria for the output capacitor is 47.7 $\mu\text{F}$ . Considering derating, two 22 $\mu\text{F}$ , 16V, X7R ceramic capacitor with 10m $\Omega$  ESR is used.

#### 8.2.2.6 Input Capacitor Selection

The LMR514x5-Q1 device requires a high frequency input decoupling capacitor or capacitor. The typical recommended value for the high frequency decoupling capacitor is 10 $\mu\text{F}$  or higher. TI recommends a high-quality ceramic type X5R or X7R with sufficiency voltage rating. The voltage rating must be greater than the maximum input voltage. To compensate the derating of ceramic capacitors, TI recommends a voltage rating of twice the maximum input voltage. For this design, two 4.7 $\mu\text{F}$ , X7R dielectric capacitor rated for 50V is used for the input decoupling capacitor. The equivalent series resistance (ESR) is approximately 10m $\Omega$ . Include a capacitor with a value of 0.1 $\mu\text{F}$  for high-frequency filtering and place as close as possible to the device pins.

#### 8.2.2.7 Bootstrap Capacitor

Every LMR514x5-Q1 design requires a bootstrap capacitor,  $C_{BOOT}$ . The recommended bootstrap capacitor is 0.1 $\mu\text{F}$  and rated at 16V or higher. The bootstrap capacitor is located between the SW pin and the BOOT pin. The bootstrap capacitor must be a high-quality ceramic type with X7R or X5R grade dielectric for temperature stability.

#### 8.2.2.8 Undervoltage Lockout Setpoint

The system undervoltage lockout (UVLO) is adjusted using the external voltage divider network of  $R_{ENT}$  and  $R_{ENB}$ . The UVLO has two thresholds, one for power up when the input voltage is rising and one for power down or brown outs when the input voltage is falling. The following equation can be used to determine the  $V_{IN}$  UVLO level.

$$V_{IN\_RISING} = V_{ENH} \times \frac{R_{EBT} + R_{ENB}}{R_{ENB}} \quad (14)$$

The EN rising threshold ( $V_{ENH}$ ) for LMR514x5-Q1 is set to be 1.25V (typical). Choose a value of 21.5k $\Omega$  for  $R_{ENB}$  to minimize input current from the supply. If the desired  $V_{IN}$  UVLO level is at 6.0V, then the value of  $R_{ENT}$  can be calculated using the following equation:

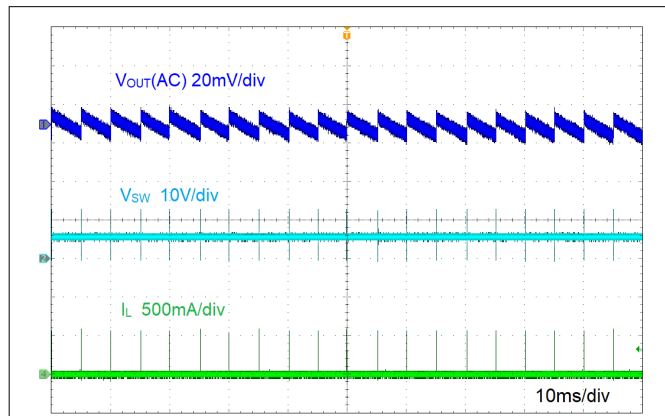
$$R_{EBT} = \left( \frac{V_{IN\_RISING}}{V_{ENH}} - 1 \right) \times R_{ENB} \quad (15)$$

The above equation yields a value of 81.7k $\Omega$ , a standard value of 82k $\Omega$  is selected. The resulting falling UVLO threshold, equals 4.8V, can be calculated by the following equation where EN hysteresis voltage,  $V_{EN\_HYS}$ , is 0.25V (typical).

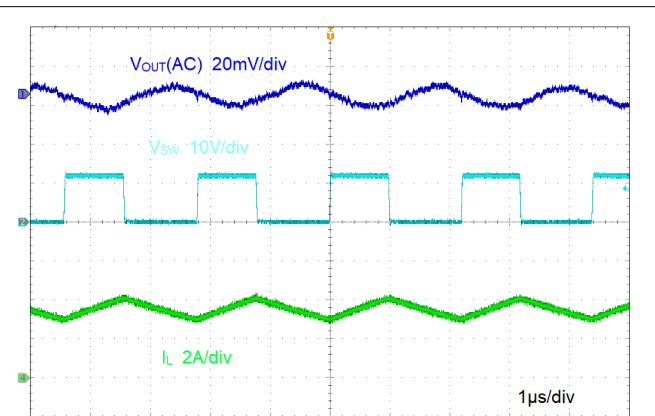
$$V_{IN\_FALLING} = (V_{ENH} - V_{ENH\_HYS}) \times \frac{R_{EBT} + R_{ENB}}{R_{ENB}} \quad (16)$$

### 8.2.3 Application Curves

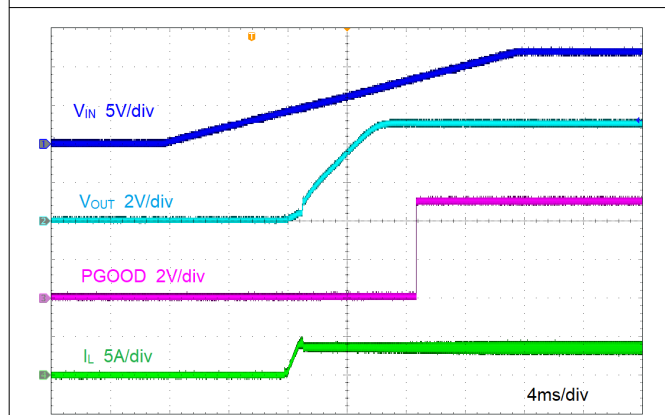
Unless otherwise specified the following conditions apply:  $V_{IN} = 12V$ ,  $V_{OUT} = 5V$ ,  $f_{SW} = 440kHz$ ,  $L = 6.8\mu H$ ,  $C_{OUT} = 47\mu F$ ,  $T_A = 25^\circ C$ .



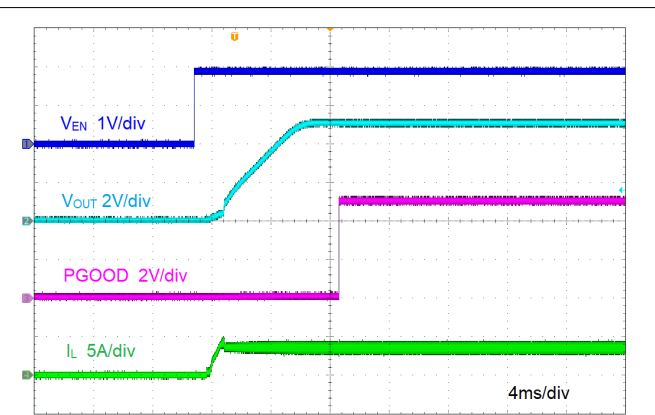
**Figure 8-2. Ripple at No Load**



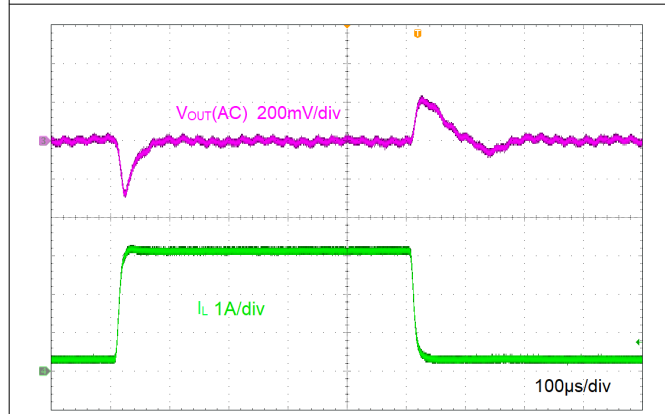
**Figure 8-3. Ripple at Full Load**



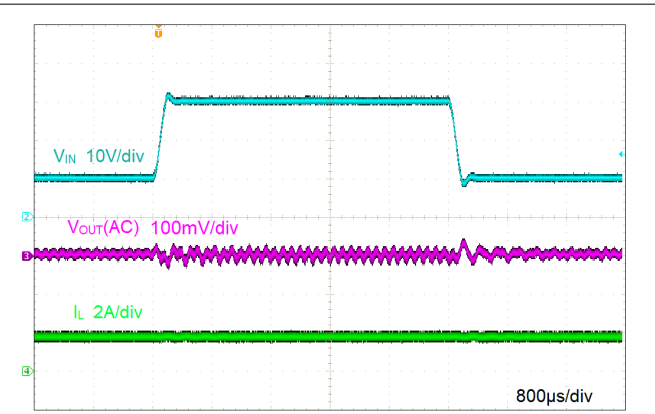
**Figure 8-4. Start-Up by  $V_{IN}$**



**Figure 8-5. Start-Up by EN**

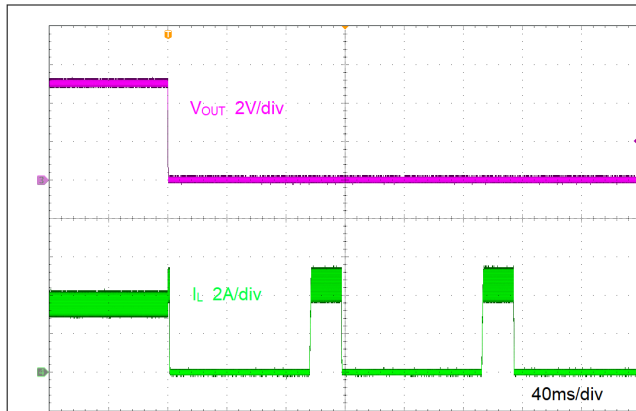


**Figure 8-6. Load Transient**

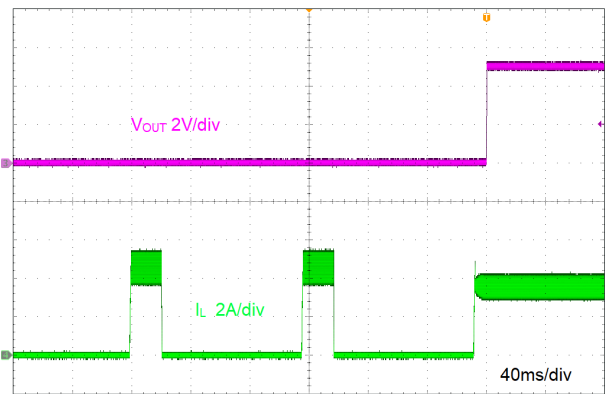


**Figure 8-7. Line Transient**





**Figure 8-8. Short Protection**



**Figure 8-9. Short Recovery**

### 8.3 Power Supply Recommendations

The LMR514x5-Q1 is designed to operate from an input voltage supply range between 4V and 36V. This input supply must be well-regulated and able to withstand maximum input current and maintain a stable voltage. The resistance of the input supply rail must be low enough that an input current transient does not cause a high enough drop at the LMR514x5-Q1 supply voltage that can cause a false UVLO fault triggering and system reset. If the input supply is located more than a few inches from the LMR514x5-Q1 additional bulk capacitance can be required in addition to the ceramic bypass capacitors. The amount of bulk capacitance is not critical, but a 47 $\mu$ F to 100 $\mu$ F electrolytic capacitor is a typical choice.

### 8.4 Layout

#### 8.4.1 Layout Guidelines

Layout is a critical portion of good power supply design. The following guidelines help users design a PCB with the best power conversion performance, thermal performance, and minimized generation of unwanted EMI.

1. Place the input bypass capacitor  $C_{IN}$  as close as possible to the VIN and PGND pins. Grounding for both the input and output capacitors must consist of localized top side planes that connect to the PGND pin.
2. Minimize trace length to the FB pin net. Both feedback resistors,  $R_{FBT}$  and  $R_{FBB}$ , must be located close to the FB pin. If  $V_{OUT}$  accuracy at the load is important, make sure  $V_{OUT}$  sense is made at the load. Route  $V_{OUT}$  sense path away from noisy nodes and preferably through a layer on the other side of a shielded layer.
3. Use ground plane in one of the middle layers as noise shielding and heat dissipation path if possible.
4. Make  $V_{IN}$ ,  $V_{OUT}$ , and ground bus connections as wide as possible. This action reduces any voltage drops on the input or output paths of the converter and maximizes efficiency.
5. Provide adequate device heat-sinking. Use an array of heat-sinking vias to connect the top side ground plane to the ground plane on the bottom PCB layer. If the PCB has multiple copper layers, these thermal vias can also be connected to inner layer heat-spreading ground planes. Make sure enough copper area is used for heat-sinking to keep the junction temperature below 150°C.

##### 8.4.1.1 Compact Layout for EMI Reduction

Radiated EMI is generated by the high di/dt components in pulsing currents in switching converters. The larger area covered by the path of a pulsing current, the more EMI is generated. High frequency ceramic bypass capacitors at the input side provide primary path for the high di/dt components of the pulsing current. Placing a ceramic bypass capacitor or capacitors as close as possible to the VIN and PGND pins is the key to EMI reduction.

The SW pin connecting to the inductor must be as short as possible, and just wide enough to carry the load current without excessive heating. Short, thick traces or copper pours (shapes) must be used for high current conduction path to minimize parasitic resistance. The output capacitors must be placed close to the  $V_{OUT}$  end of the inductor and closely grounded to PGND pin.

#### 8.4.1.2 Feedback Resistors

To reduce noise sensitivity of the output voltage feedback path, make sure to place the resistor divider close to the FB pin, rather than close to the load. The FB pin is the input to the error amplifier, so the FB pin is a high impedance node and very sensitive to noise. Placing the resistor divider closer to the FB pin reduces the trace length of FB signal and reduces noise coupling. The output node is a low impedance node, so the trace from  $V_{OUT}$  to the resistor divider can be long if short path is not available.

If voltage accuracy at the load is important, make sure voltage sense is made at the load. Doing so corrects for voltage drops along the traces and provides the best output accuracy. The voltage sense trace from the load to the feedback resistor divider must be routed away from the SW node path and the inductor to avoid contaminating the feedback signal with switch noise, while also minimizing the trace length. This is most important when high value resistors are used to set the output voltage. TI recommends to route the voltage sense trace and place the resistor divider on a different layer than the inductor and SW node path, such that there is a ground plane in between the feedback trace and inductor/SW node polygon. This action provides further shielding for the voltage feedback path from EMI noises.

### 8.4.2 Layout Example

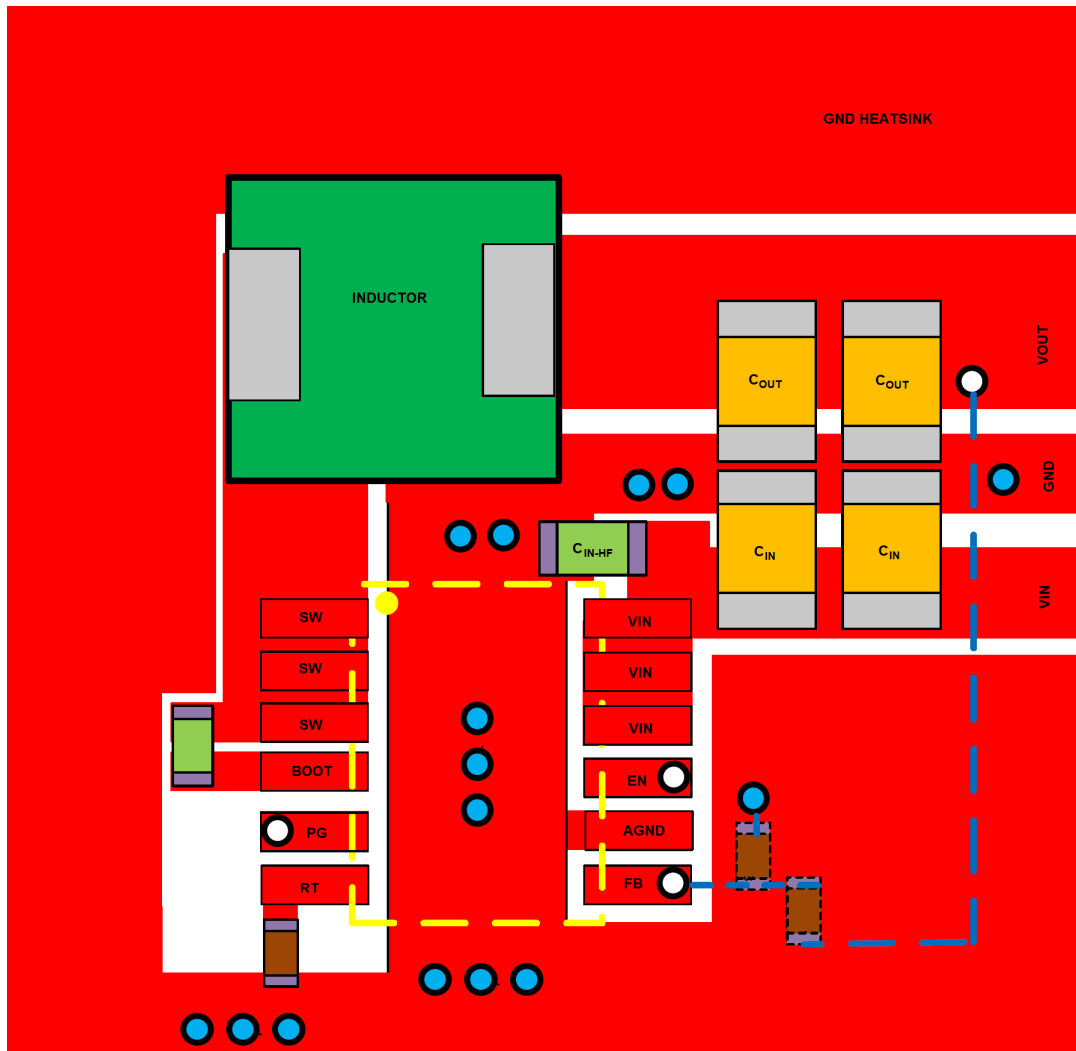


Figure 8-10. Layout

## 9 Device and Documentation Support

### 9.1 Device Support

#### 9.1.1 Development Support

##### 9.1.1.1 Custom Design With WEBENCH® Tools

[Click here](#) to create a custom design using the LMR514x5-Q1 device with the WEBENCH® Power Designer.

1. Start by entering the input voltage ( $V_{IN}$ ), output voltage ( $V_{OUT}$ ), and output current ( $I_{OUT}$ ) requirements.
2. Optimize the design for key parameters such as efficiency, footprint, and cost using the optimizer dial.
3. Compare the generated design with other possible solutions from Texas Instruments.

The WEBENCH Power Designer provides a customized schematic along with a list of materials with real-time pricing and component availability.

In most cases, these actions are available:

- Run electrical simulations to see important waveforms and circuit performance
- Run thermal simulations to understand board thermal performance
- Export customized schematic and layout into popular CAD formats
- Print PDF reports for the design, and share the design with colleagues

Get more information about WEBENCH tools at [www.ti.com/WEBENCH](http://www.ti.com/WEBENCH).

### 9.2 Documentation Support

#### 9.2.1 Related Documentation

For related documentation see the following:

- Texas Instruments, [Layout Guidelines for Switching Power Supplies application note](#)
- Texas Instruments, [A Guide to Board Layout for Best Thermal Resistance for Exposed Pad Packages application note](#)
- Texas Instruments, [How to Properly Evaluate Junction Temperature with Thermal Metrics application note](#)

### 9.3 Receiving Notification of Documentation Updates

To receive notification of documentation updates, navigate to the device product folder on [ti.com](http://ti.com). Click on *Notifications* to register and receive a weekly digest of any product information that has changed. For change details, review the revision history included in any revised document.

### 9.4 Support Resources

[TI E2E™ support forums](#) are an engineer's go-to source for fast, verified answers and design help — straight from the experts. Search existing answers or ask your own question to get the quick design help you need.

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### 9.5 Trademarks

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### 9.6 Electrostatic Discharge Caution



This integrated circuit can be damaged by ESD. Texas Instruments recommends that all integrated circuits be handled with appropriate precautions. Failure to observe proper handling and installation procedures can cause damage.

ESD damage can range from subtle performance degradation to complete device failure. Precision integrated circuits may be more susceptible to damage because very small parametric changes could cause the device not to meet its published specifications.

### 9.7 Glossary

[TI Glossary](#) This glossary lists and explains terms, acronyms, and definitions.

## 10 Revision History

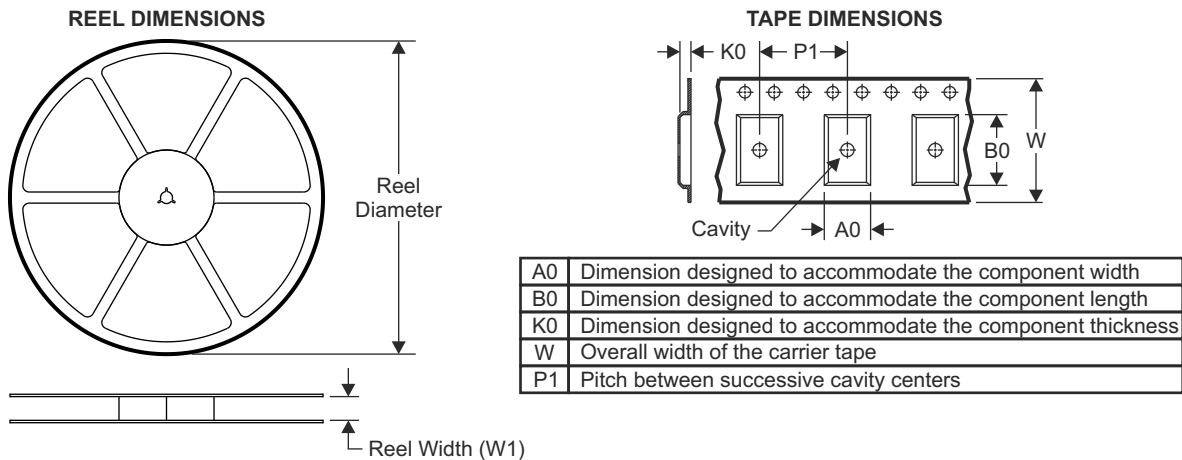
NOTE: Page numbers for previous revisions may differ from page numbers in the current version.

DATE	REVISION	NOTES
September 2024	*	Initial release

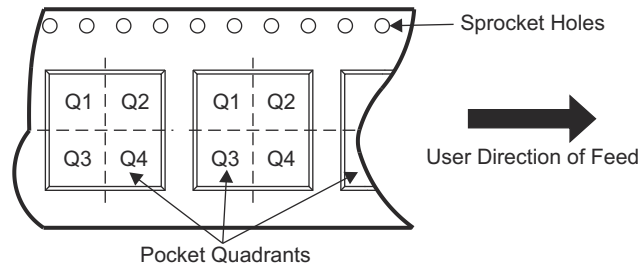
## 11 Mechanical, Packaging, and Orderable Information

The following pages include mechanical, packaging, and orderable information. This information is the most current data available for the designated devices. This data is subject to change without notice and revision of this document. For browser-based versions of this data sheet, refer to the left-hand navigation.

### 11.1 Tape and Reel Information

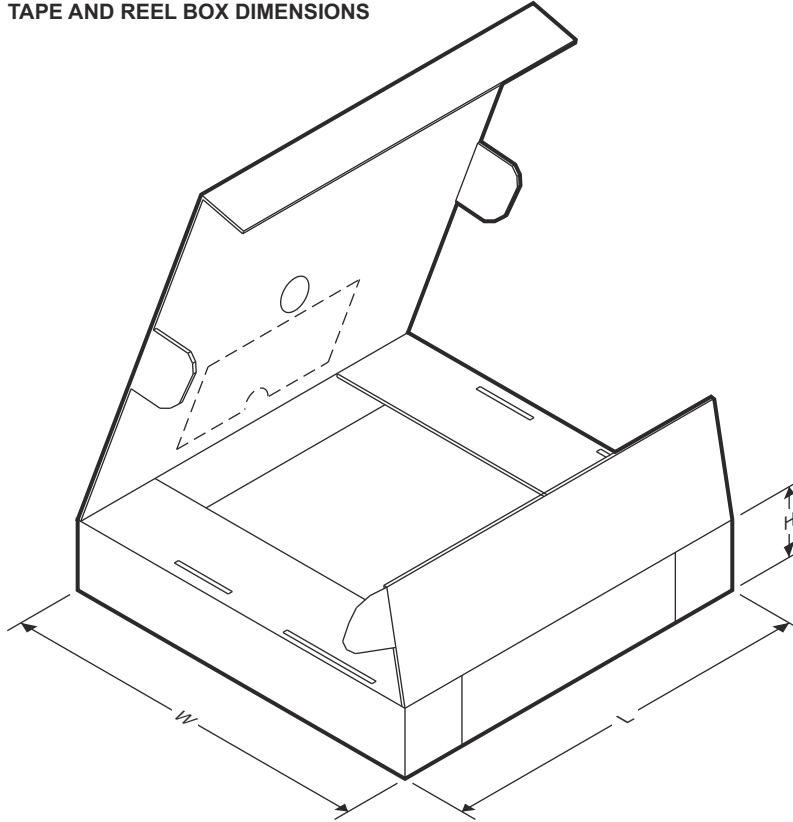


#### QUADRANT ASSIGNMENTS FOR PIN 1 ORIENTATION IN TAPE



Device	Package Type	Package Drawing	Pins	SPQ	Reel Diameter (mm)	Reel Width W1 (mm)	A0 (mm)	B0 (mm)	K0 (mm)	P1 (mm)	W (mm)	Pin1 Quadrant
LMR51435SQDRRRQ1	WSO	DRR	12	3000	330.0	12.4	3.3	3.3	1.1	8.0	12.0	Q2
LMR51435FSQDRRRQ1	WSO	DRR	12	3000	330.0	12.4	3.3	3.3	1.1	8.0	12.0	Q2
LMR51425SQDRRRQ1	WSO	DRR	12	3000	330.0	12.4	3.3	3.3	1.1	8.0	12.0	Q2
LMR51425FSQDRRRQ1	WSO	DRR	12	3000	330.0	12.4	3.3	3.3	1.1	8.0	12.0	Q2

**TAPE AND REEL BOX DIMENSIONS**



Device	Package Type	Package Drawing	Pins	SPQ	Length (mm)	Width (mm)	Height (mm)
LMR51435SQDRRRQ1	WSON	DRR	12	3000	367.0	367.0	35.0
LMR51435FSQDRRRQ1	WSON	DRR	12	3000	367.0	367.0	35.0
LMR51425SQDRRRQ1	WSON	DRR	12	3000	367.0	367.0	35.0
LMR51425FSQDRRRQ1	WSON	DRR	12	3000	367.0	367.0	35.0

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